FEATURES
- Reverse Input Protection to −40V
- Improved Performance Compared to a Schottky Diode
- Reduce Power Dissipation by >90%
- Reduce Drop to 20mV
- Ultrafast Transient Response
  - Rectifies 6V_{P-P} Up to 50kHz
  - Rectifies 2V_{P-P} Up to 100kHz
- Wide Operating Voltage Range: 3V to 42V
- Low 20μA Quiescent Current in Operation
- Low 3.5μA Shutdown Current
- Accurate 1.21V Enable Pin Threshold
- Small 10-Lead MSOP Package or 10-Lead 3mm × 2mm DFN Package

APPLICATIONS
- Automotive Battery Protection
- Industrial Supplies
- Portable Instrumentation

DESCRIPTION
The LT®8672 is an active rectifier controller for reverse input protection. It drives an external N-channel MOSFET to replace a power Schottky diode. Its very low quiescent current and fast transient response meet the tough requirements in automotive applications where AC input signals of up to 100kHz are present. These signals are rectified with minimum power dissipation on the external FET, simplifying thermal management on the PCB.

With a drop of only 20mV, the LT8672 solution eases the minimum input voltage requirement during cold crank and start-stop, allowing simpler and more efficient circuits. If the input power source fails or is shorted, a fast turn-off minimizes reverse current transients. An available shutdown mode reduces the quiescent current to 3.5μA.

An integrated auxiliary boost regulator provides the required boost voltage to turn the external FET fully on. A power good pin signals when the external FET is ready to take load current.

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ABSOLUTE MAXIMUM RATINGS
(Notes 1 and 2)

DRAIN .......................................................... –0.3V to 42V
SOURCE, EN/UVLO ........................................ –40V to 42V
DRAIN–SOURCE ............................................ –5V to 54V
AUX ............................................................. \( V_{\text{DRAIN}} + 13V \)
GATE .......................... \( V_{\text{SOURCE}} – 0.3V \) to \( V_{\text{SOURCE}} + 17V \)
GATE .................................. \( V_{\text{AUX}} – 67V \) to \( V_{\text{AUX}} + 0.3V \)
PG ............................................................... –0.3V to 5V

Operating Junction Temperature Range (Notes 3, 4)

E-, I-Grades ........................................... –40°C to 125°C
J-, H-Grades ........................................... –40°C to 150°C

Storage Temperature Range ............. –65°C to 150°C

Lead Temperature (Soldering, 10 sec)

MS Package .................................................... 300°C

Tape and Reel Specifications. Some packages are available in 500 unit reels through designated sales channels with #TRMPBF suffix.

ORDER INFORMATION

Contact the factory for parts specified with wider operating temperature ranges. *The temperature grade is identified by a label on the shipping container.

**For more information www.analog.com**
**ELECTRICAL CHARACTERISTICS**

The ● denotes the specifications which apply over the full operating temperature range, otherwise specifications are at $T_A = 25°C$. $V_{\text{SOURCE}} = V_{\text{DRAIN}} = 12V$, unless otherwise noted. (Note 3)

<table>
<thead>
<tr>
<th>PARAMETER</th>
<th>CONDITIONS</th>
<th>MIN</th>
<th>TYP</th>
<th>MAX</th>
<th>UNITS</th>
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</thead>
<tbody>
<tr>
<td>Minimum Drain Voltage</td>
<td>$V_{\text{EN/UVLO}} = 0V$</td>
<td>2.85</td>
<td>3</td>
<td></td>
<td>V</td>
</tr>
<tr>
<td>Total System Quiescent Current</td>
<td>$V_{\text{EN/UVLO}} = 0V$</td>
<td>●</td>
<td>3.5</td>
<td>5</td>
<td>µA</td>
</tr>
<tr>
<td></td>
<td>$V_{\text{EN/UVLO}} = 2V$, Active Rectifier Controller In Regulation (Note 4)</td>
<td>●</td>
<td>20</td>
<td>26</td>
<td>µA</td>
</tr>
<tr>
<td>EN/UVLO Pin Threshold High</td>
<td>Pin Voltage Rising</td>
<td>1.22</td>
<td>1.28</td>
<td>1.34</td>
<td>V</td>
</tr>
<tr>
<td>EN/UVLO Pin Threshold Low</td>
<td>Pin Voltage Falling</td>
<td>1.16</td>
<td>1.21</td>
<td>1.26</td>
<td>V</td>
</tr>
<tr>
<td>EN/UVLO Pin Hysteresis</td>
<td></td>
<td>70</td>
<td></td>
<td></td>
<td>mV</td>
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<tr>
<td>EN/UVLO Pin Current</td>
<td>$V_{\text{EN/UVLO}} = 2V$</td>
<td></td>
<td></td>
<td>−0.1</td>
<td>µA</td>
</tr>
<tr>
<td>PG Pin Leakage</td>
<td>$V_{\text{PG}} = 3.3V$</td>
<td>−0.1</td>
<td></td>
<td>0.1</td>
<td>µA</td>
</tr>
<tr>
<td>PG Pull-Down Resistance</td>
<td>$V_{\text{PG}} = 0.1V$</td>
<td>●</td>
<td>650</td>
<td>2000</td>
<td>Ω</td>
</tr>
</tbody>
</table>

**Auxiliary Boost Regulator**

- **Regulation Voltage $V_{\text{AUX}} - V_{\text{DRAIN}}$**
- **Power NMOS Current Limit**
- **Power NMOS On-Resistance**
- **Catch Diode Forward Voltage** $I_{\text{DIODE}} = 100mA$
- **AUXSW Pin Leakage** $V_{\text{AUXSW}} = 12V$

**Active Rectifier Controller**

- **SOURCE–DRAIN Regulation Voltage**
- **SOURCE–DRAIN Fast Pull-Up Threshold**
- **DRAIN Current** With Gate Driver in Regulation
- **SOURCE Current** With Gate Driver in Regulation
- **Maximum Gate Drive (GATE–SOURCE)**
- **Gate Pull-Up Current**
- **Gate Pull-Down Current**
- **Gate-Source Off Voltage for Reverse SOURCE** Fault Condition, $V_{\text{SOURCE}} = −5V$, $I_{\text{GATE}} = 1mA$
- **Gate Turn-Off Delay Time**
- **Gate Turn-On Delay Time**
- **Maximum Frequency of AC Input Signal to Be Rectified** AC Input Ripple ≤ 6V p-p, $C_{\text{GATE–SOURCE}} = 10nF$

**Note 1:** Stresses beyond those listed under Absolute Maximum Ratings may cause permanent damage to the device. Exposure to any Absolute Maximum Rating condition for extended periods may affect the device reliability and lifetime.

**Note 2:** Positive currents flow into pins, negative currents flow out of pins. Minimum and Maximum values refer to absolute values.

**Note 3:** LT8672E is guaranteed to meet performance specifications from 0°C to 125°C junction temperature. Specifications over the −40°C to 125°C operating junction temperature range are assured by design, characterization and correlation with statistical process controls. LT8672I is guaranteed over the full −40°C to 125°C operating junction temperature range. The LT8672J and the LT8672H are guaranteed over the full −40°C to 150°C operating junction temperature range.

**Note 4:** Total system current with active rectifier controller in regulation.
TYPICAL PERFORMANCE CHARACTERISTICS

Total Input Current in Regulation

Total Input Current in Shutdown

GATE Current vs Forward Voltage Drop

Fast Pull-Down Current

Fast Pull-Up Current

Forward Regulation Voltage

GATE Turn-Off Time vs GATE Capacitance

GATE Turn-On Time vs GATE Capacitance

Fast Pull-Down Threshold

For more information www.analog.com
TYPICAL PERFORMANCE CHARACTERISTICS

Fast Pull-Up Threshold

AUX–DRAIN Regulation Voltage

Auxiliary Boost Regulator Current Limit

EN/UVLO Pin Thresholds

Fast Pull-Up to PG Low Delay

Dropout Performance

Auxiliary Boost Regulator Switching Waveforms

Auxiliary Boost Regulator Response to Fast Pull-Up

For more information www.analog.com
PIN FUNCTIONS

EN/UVLO (Pin 1): The LT8672’s active rectifier controller and the auxiliary boost regulator are shut down when this pin is below 1.21V. Tie to DRAIN if this shutdown feature is not used.

GND (Pin 2): This pin has no function in the application and should be connected to ground.

PG (Pin 3): The PG pin is the open drain output of an internal monitor circuitry. PG pulls low if any of the following criteria is met: the part is in shutdown, the AUX voltage has not reached its regulation value during start-up or the gate driver’s fast pull-up path is active for more than 17µs. If the PG pin is used to control the output load, it can protect the MOSFET from being overloaded under these conditions. PG output is valid when DRAIN is above the minimum input voltage.

GND (Pin 4): This is the ground of all the internal circuitry. Tie directly to the local GND plane.

NC (Pin 5): This pin is not connected internally. Connect it to ground or leave it floating.

AUXSW (Pin 6): Output of the Internal Power Switch of the Auxiliary Boost Regulator. This node should be kept small on the PCB for good performance and low EMI. Connect the boost inductor between this pin and the DRAIN pin.

AUX (Pin 7): Auxiliary Boost Regulator Output. This pin is used to provide a drive voltage, higher than the input voltage, to the gate driver of the active rectifier controller. Connect a 1µF capacitor between this pin and the DRAIN pin as close as possible to the IC. Do not place a capacitor to any other node than DRAIN on this pin.

DRAIN (Pin 8): Drain Voltage Sense and Supply Voltage. The voltage sensed at this pin is used to control the external MOSFET gate. It also provides current to the LT8672’s internal circuitry. Connect this pin as close as possible to the drain of the external N-channel MOSFET. This pin must be locally bypassed with at least 4.7µF.

SOURCE (Pin 9): Source Connection. SOURCE is the return path of the gate fast pull-down. The voltage sensed at this pin is also used to control the MOSFET gate. Connect this pin as close as possible to the source of the external N-channel MOSFET.

GATE (Pin 10): Gate Drive Output. This pin drives the gate of the external N-channel MOSFET. Connect this pin to the gate of the MOSFET.

Exposed Pad (Pin 11, DFN Only): The exposed pad must either be left floating or be connected to the GND pin.
The LT8672 is an active rectifier controller including an integrated auxiliary boost regulator for fast turn on of the external N-channel MOSFET. Operation is best understood by referring to the Block Diagram.

**Active Rectifier Controller**

The active rectifier controller controls an external N-channel MOSFET (M1) to form an ideal diode. The GATE amplifier senses across DRAIN and SOURCE and drives the gate of the MOSFET to regulate the forward voltage to 20mV. As the load current increases, GATE is driven higher until a point is reached where the MOSFET is fully on. If the load current is reduced, the GATE amplifier drives the MOSFET gate lower to maintain a 20mV drop. If the voltage $V_{DRAIN}$ is reduced to a point where a forward drop of 20mV cannot be supported, the GATE amplifier drives the MOSFET off.

During fast SOURCE–DRAIN transients such as fast varying input (SOURCE) signals where the regulating 20mV loop is too slow, fast pull-up (FPU) and fast pull-down (FPD) current paths turn on and off the external MOSFET quickly. This rectifies the input signal the same way a diode would do but with much less power dissipation.

The SOURCE and GATE pins are protected against reverse input voltages of up to –40V. GATE is pulled to SOURCE when SOURCE goes negative, turning off the MOSFET and isolating DRAIN from the negative input.

The gate voltage for the external MOSFET is provided by the auxiliary boost regulator, which regulates its output AUX to 11V above DRAIN.

The EN/UVLO pin can be used to shut down the active rectifier controller and auxiliary boost regulator. By setting EN/UVLO low, total system input current is reduced to less than 3.5µA. The conduction path on the external MOSFET would only be through its body diode.

**Auxiliary Boost Regulator**

The auxiliary boost regulator uses a hysteretic control scheme in conjunction with a constant low side current limit of 100mA. When the AUX–DRAIN voltage is below its nominal value of typically 11V, the low side power switch is turned on. The $L_{AUX}$ inductor current rises, until it reaches the low side current limit of 100mA, at which point the low side switch is turned off and the inductor discharges into $C_{AUX}$ until its current falls to zero. Then, the low side switch turns on again, unless the AUX–DRAIN voltage has risen above its nominal value. In this case, all high power circuitry is shut off in order to reduce the quiescent current.

This control scheme results in a switching frequency which depends on inductor value and DRAIN voltage.

**Power Good Pin (PG)**

The open drain power good pin PG goes high impedance when no fault is present. This indicates the external MOSFET is operating properly.
Active Rectifier Controller

Blocking diodes are commonly placed in series with supply inputs to protect against supply reversal. The LT8672 replaces diodes in these applications with a MOSFET to reduce both the voltage drop and power loss associated with a passive solution. The curve shown in Figure 1 illustrates the dramatic improvement in power loss achieved in a practical application. This represents significant savings in board area by greatly reducing power dissipation in the pass device. At low input voltages, the improvement in forward voltage loss is readily appreciated where headroom is tight, as shown in Figure 2.

The LT8672 operates from 3V to 42V and withstands an absolute maximum range of -40V to 42V without damage. In automotive applications the LT8672 operates through load dump, cold crank and two-battery jumps, and it survives reverse battery connections while also protecting the load. Furthermore, due to its fast response to changes in the external MOSFET’s forward voltage, it can rectify input ripple with amplitudes as high as 6V P-P up to 50kHz. Rectification up to 100kHz is possible with amplitudes as high as 2V P-P. The fast gate drive capability of the LT8672 prevents the external MOSFET from overheating during these demanding conditions since its body diode conducts current only for a very small portion of the ripple period.

The LT8672 does not require any bypass capacitor at the SOURCE pin (C_{BYP} in the Block Diagram). Should such a capacitor be needed for other reasons, for example as part of an up-front EMI filter, its capacitance must not exceed 60nF; otherwise, the gate driver’s stability may be impaired. This applies to the total capacitance connected to SOURCE on the PCB.

It is important to note that the EN/UVLO pin, while disabling the LT8672 and reducing its current consumption to 3.5μA, does not disconnect the load from the input since the MOSFET’s body diode is ever-present.

Shutdown Mode/Undervoltage Lockout

In shutdown, the LT8672 pulls GATE low to SOURCE, turning off the MOSFET and reducing current consumption to 3.5μA. Shutdown does not interrupt forward current flow; a path is still present through M1’s body diode. When enabled, the LT8672 operates as an active rectifier. If shutdown is not needed, connect EN/UVLO to DRAIN. EN/UVLO may be driven with a 3.3V or 5V logic signal. To disable the part, EN/UVLO must be pulled down below 1.21V.
Adding a resistive divider from SOURCE to EN/UVLO, as shown in Figure 3, programs the LT8672 to disable itself when \( V_{\text{BATT}} \) is below a threshold voltage \( V_{\text{BATT(EN/UVLO)}} \), given by:

\[
R_1 = R_2 \left( \frac{V_{\text{BATT(EN/UVLO)}}}{1.21V} - 1 \right)
\]

The EN/UVLO Pin Allows Programmable Undervoltage Lockout

Note that due to the comparator’s hysteresis, the LT8672 will not be enabled until \( V_{\text{BATT}} \) rises slightly above \( V_{\text{BATT(EN/UVLO)}} \). If EN/UVLO is connected using a high ohmic resistor, it is subject to capacitive coupling from nearby clock lines or traces exhibiting high dV/dt. Bypass EN/UVLO to GND with 1nF to eliminate injection.

This capacitor, if sized accordingly, will also prevent negative voltage transients on \( V_{\text{BATT}} \) from inadvertently disabling the LT8672.

Input Short-Circuit Faults and Negative Transients

For fast negative input transients, the LT8672 relies on its fast pull-down (FPD) comparator. But since the FPD threshold is negative, reverse current is built up in the external MOSFET prior to an FPD turn-off. This process resembles the reverse recovery of a diode, although cause and timing differ. Since there is always a parasitic or, in case of an up front EMI filter, intended inductance in front of SOURCE, the reverse current stores energy in this inductance. This energy pulls the SOURCE node negative, once the external MOSFET is finally turned off. A zero impedance short-circuit directly across the input and ground is especially troublesome because it permits the highest possible reverse current to build up.

This negative transient on SOURCE may potentially be destructive to the LT8672, since the voltage on the SOURCE pin is limited to –40V. To prevent damage to the LT8672, protect the SOURCE pin as shown in Figure 4 by clamping to the ground node with two TVS diodes. Negative spikes, seen after the MOSFET turns off during an FPD event, are clamped by D2. The example, a 15V TVS, is a good choice for automotive applications, where a reversed battery could produce a reverse voltage of up to 14.4V, at which D2 should not conduct any current. D2 is not required if reverse-input protection is not needed.
APPLICATIONS INFORMATION

D1 protects SOURCE in the positive direction during load steps and overvoltage conditions. The example, a 33V TVS, is a good choice for automotive applications, where a load dump could produce an overvoltage at which D1 should not conduct any current.

If neither D1 nor any reverse current protection (D2) is needed, a diode is still required at SOURCE to protect the LT8672 from negative inductive spikes caused by any parasitic input inductance.

For input voltages 4V greater than $V_{GS(MAX)}$ of the external MOSFET, a direct short (minimal inductance of less than a few nH) at the SOURCE node on the PCB could temporarily increase the $V_{GS}$ of the external MOSFET above its $V_{GS(MAX)}$. If such a short is to be expected, D3 is needed to protect the external MOSFET.

Any leakage current in D3 will increase the total quiescent current accordingly. In addition, D3’s leakage current should not exceed 5µA, as it would otherwise create an offset at the gate driver’s input, increasing the SOURCE–DRAIN regulation voltage.

Rectification of Fast Input Ripple

The LT8672 is specifically designed to address the challenging specifications for battery connected automotive electronic control units (ECUs). For example, according to automotive norms ISO16750 or LV124 an ECU may be subjected to an AC ripple superimposed on its supply, with frequencies of up to 30kHz and amplitudes of up to 6Vp-p.

Due to its gate driver’s high output current and short delay times, the LT8672 is able to control the external MOSFET rapidly enough even at these frequencies to keep power dissipation and reverse current conduction to a minimum. In addition, this significantly reduces the ripple current in the output capacitor.

Figure 5, Figure 6 and Figure 7 show input and output waveforms for various input ripple frequencies.
APPLICATIONS INFORMATION

MOSFET Selection

All load current passes through an external MOSFET, M1. The important characteristics of the MOSFET are on-resistance, \( R_{\text{DS(ON)}} \), the maximum drain-source voltage, \( V_{\text{DS}} \), the gate threshold voltage \( V_{\text{GS(TH)}} \) and the total gate charge \( Q_{\text{GTOT}} \).

Gate drive is compatible with standard threshold and logic-level MOSFETs over the entire operating range of 3V to 42V. For logic-level MOSFETs, \( V_{\text{GS(MAX)}} \) should be \( \pm15V \) or higher.

The maximum allowable drain-source voltage, \( V_{\text{DS}} \), must be higher than the power supply voltage. If the input is grounded, the full supply voltage will appear across the MOSFET. If the input is reversed and the output is held up by a charged capacitor, battery or power supply, the sum of the input and output voltages will appear across the MOSFET and require a \( V_{\text{DS}} > V_{\text{OUT}} + |V_{\text{BATT}}| \).

The MOSFET’s on-resistance, \( R_{\text{DS(ON)}} \), directly affects the forward voltage drop and power dissipation. Desired forward voltage drop should be less than that of a diode for reduced power dissipation; 60mV is a good starting point. Choose a MOSFET which has:

\[
R_{\text{DS(ON)}} < \frac{\text{Forward Voltage Drop}}{I_{\text{LOAD}}} 
\]

The resulting power dissipation is

\[
P_d = I_{\text{LOAD}}^2 \times R_{\text{DS(ON)}}
\]

For fast gate drive operation choose a MOSFET with the smallest total gate charge \( Q_{\text{GTOT}} \) that also satisfies the \( V_{\text{DS}} \) and \( R_{\text{DS(ON)}} \) requirements. A MOSFET with smaller \( Q_{\text{GTOT}} \) not only reduces reverse current during the turn-off phase but also stays cooler during rectification of high amplitude ripple on the input.

If the MOSFET has an integrated gate protection, its leakage should not exceed 5µA, as this would otherwise create an offset at the gate driver’s input, increasing the SOURCE–DRAIN regulation voltage.

When the LT8672 rectifies an AC ripple voltage, the average current through the external MOSFET still equals the load current, but the peak current is much higher. Since the MOSFET’s power dissipation is proportional to the square of this current as described above, the average power dissipation during rectification exceeds the power dissipation in steady state. The actual peak current depends on the external components and their parasitics. Figure 8 shows a simple model which can be used to estimate the peak current by computer simulation. \( R_{\text{BATT}} \) represents the impedance of the voltage source \( V_{\text{BATT}} \), the inductor models the combined inductance of the cable and, if present, the EMI filter inductor. The ideal diode has no resistance and a forward voltage of 0V. \( R_{\text{DS(ON)}} \) represents the on-resistance of the external MOSFET, while \( C_{\text{LOAD}} \) and \( R_{\text{ESR}} \) represent the electrolytic capacitor and its equivalent series resistance.

![Figure 8. Simplified Application Model Including All Relevant Parasitics](image-url)
APPLICATIONS INFORMATION

For example, an application with $C_{LOAD} = 470\mu F$, $R_{ESR} = 16\, \text{m}\Omega$, $R_{DS(ON)} = 5\, \text{m}\Omega$, $L_{CABLE} + L_{EMI} = 1\, \mu\text{H}$, and $R_{BATT} = 50\, \text{m}\Omega$ dissipates 0.5W of power in steady state with a load current of 10A. But this power increases to 1.13W when a 6V$_{P-P}$ AC-ripple with a frequency of 10kHz is superimposed on $V_{BATT}$. Removing any inductance raises this power even further to 1.3W, while the RMS current in $C_{LOAD}$ reaches 12.6A.

This model can also be used to select an electrolytic capacitor which can handle the corresponding RMS current for the duration of the AC-ripple.

Electrolytic Capacitor and Ripple Voltage

During rectification, the electrolytic capacitor $C_{LOAD}$ reduces the ripple voltage seen by the load. Figure 9 shows the corresponding waveforms for the rectification of a sinusoidal SOURCE ripple voltage.

For example, if the ripple voltage $V_R$ is to be kept below 2V at $f = 5kHz$, $V_{AC} = 3V$ (6V$_{P-P}$), and a load current of $I_{LOAD} = 5A$, then $C_{LOAD} = 417\mu F$.

When selecting an electrolytic capacitor also keep in mind the high peak currents at high frequencies as discussed in the previous section.

Automotive Cold Crank

During the so-called “cold crank” (e.g. LV124 E-11) a car’s battery voltage may drop to 3.2V. As a result, the high voltage drop of traditional reverse protection schemes using passive rectifiers like Schottky diodes require the supplied circuitry to work at minimum input voltages as low as 2.5V. Buck-boost regulators may then be needed instead of simpler and more efficient buck regulators in order to provide a stable 3V supply often required by many microcontrollers.

The LT8672’s minimum input operating voltage of 3V allows the active rectifier to operate through the cold crank pulse with minimum drop between input and output. This allows use of a buck regulator with a minimum operating voltage of 3V and low dropout characteristics like the LT8650S to generate a 3V supply.

Figure 10 shows input and output waveforms during a cold crank pulse, comparing the LT8672 active rectifier controller to a Schottky diode.
**APPLICATIONS INFORMATION**

**Figure 10. Automotive Cold Crank Waveforms**

**Auxiliary Boost Regulator**

The auxiliary boost regulator provides a boosted voltage to the gate driver to enhance the external MOSFET fully with at least 10V of gate drive.

It uses a hysteretic control scheme in conjunction with a constant low side current limit of 100mA. This control scheme results in a switching frequency with a maximum value which depends on inductor value and DRAIN voltage.

Recommended boost regulator external passive components are a 1μF/16V ceramic capacitor and a 47μH to 100μH inductor. The inductor’s saturation current should be at least 120mA and its ESR should not exceed 10Ω, therefore small chip inductors like CBC2518T470K or CBC2518T101K from Taiyo Yuden or those from the XPL2010 series from Coilcraft are good options.

The boost regulator maximum output current available to the gate driver on the AUX pin can be approximated by the following equation:

$$I_{AUX(MAX)} = 50 \cdot \frac{V_{DRAIN} - 1}{V_{DRAIN} + 11.8}$$

where $I_{AUX(MAX)}$ is the maximum boost regulator output current in mA and $V_{DRAIN}$ is the DRAIN pin voltage in volts.

This maximum available AUX current is achieved at the boost regulator’s maximum switching frequency which can be approximated by following equation:

$$f_{AUXSW(MAX)} = \frac{1180 \cdot (V_{DRAIN} - 0.2)}{(V_{DRAIN} + 11.6) \cdot (10L_{AUX} + 3V_{DRAIN} - 0.6)}$$

where $f_{AUXSW(MAX)}$ is the maximum switching frequency in MHz, $V_{DRAIN}$ is the DRAIN pin voltage in volts and $L_{AUX}$ is the boost regulator inductor in μH.

However, depending on the total average current required by the gate driver on the AUX pin to switch the external MOSFET on and off periodically, the boost regulator might enter discontinuous mode and switch at a lower frequency given by the following equation:

$$f_{AUXSW} = \frac{2.9 \cdot I_{AUX}}{L_{AUX}}$$

where $f_{AUXSW}$ is the switching frequency in MHz, $I_{AUX}$ is the average current required by the gate driver in mA and $L_{AUX}$ is the boost regulator inductor in µH.

During rectification of input ripple, fully charging and discharging the gate capacitance of the external MOSFET requires an average AUX current

$$I_{AUX} = \frac{f \cdot Q_G}{1000}$$

where $f$ is the ripple frequency in kHz, $Q_G$ is the total gate charge of the external MOSFET in nC, and $I_{AUX}$ is the AUX current in mA drawn by the gate driver. For example, rectification of a 6Vp-p=50kHz input ripple superimposed on the 12V battery voltage, using an external MOSFET with 100nC of total gate charge under full load conditions, requires an average turn on gate current of 5mA which the gate driver takes from the AUX pin. Under these conditions, the boost regulator runs with a switching frequency of 145kHz using a 100μH inductor. The maximum available AUX current is approximately 23mA with the boost regulator switching at about 595kHz.

When the active rectifier is in steady state conditions, the AUX pin current required by the gate driver is approximately 1μA and the boost regulator is most of the time in sleep mode.
APPLICATIONS INFORMATION

Mode waking up only from time to time to maintain the AUX pin voltage 11V above DRAIN.

Figure 11, Figure 12 and Figure 13 show typical waveforms with 1µA, 5mA, and 10mA of AUX load current.

Power Good Pin

The power good pin is the output of internal monitoring circuitry, which signals when the external MOSFET is able to pass the full load current with a voltage of less than 75mV between its source and drain. PG only goes high if the LT8672 is enabled, and the AUX voltage has reached its regulation value during start-up, and if the gate driver’s fast pull-up path is not engaged for more than 17µs. This allows detection of a number of system faults.

For example, the gate of the external MOSFET may be shorted to ground or source. It would then be impossible to turn it on, which would keep the gate driver’s fast pull-up path active indefinitely, thereby pulling PG low. The fast pull-up path would never be active for so long in a correctly working system, because charging the external MOSFET’s gate requires much less time.

An insufficient AUX voltage (for example during start-up or due to a system fault) may be able to deliver sufficient gate-source voltage to the external MOSFET for small load currents, but not for high load currents. Therefore PG is pulled low if AUX remains too low during start-up.

PG is valid (and pulls low) even in shutdown. Although this may increase the overall shutdown current through the external pull-up resistor on PG, it keeps the system correctly informed about the shutdown status of the LT8672 and that it cannot enhance the external MOSFET.

Thus, if PG is used to control the load current in the external MOSFET, its body diode can be prevented from conducting large currents for a prolonged period of time. This significantly reduces the amount of heat generated by the external MOSFET even in fault conditions.

The fast pull-up path is active when the external MOSFET’s forward voltage exceeds 75mV, therefore it is recommended to choose a MOSFET large enough not to exceed this threshold with maximum load current. If the PG flag is ignored in the application, the MOSFET can be pushed to higher forward voltages provided that its power dissipation is kept within safe levels.
The PG output is valid when DRAIN is above the minimum input voltage. Figure 14 and Figure 15 show power good pin waveforms under several “MOSFET Not Ready” conditions.

**Layout Considerations**

Connect the SOURCE and DRAIN pins as close as possible to the MOSFET source and drain pins. Keep the traces to the MOSFET wide and short to minimize resistive losses as shown in Figure 16 and Figure 17. Place surge suppressors and necessary transient protection components close to the LT8672 using short lead lengths. Keep more than minimum distance from GATE traces to other nodes to prevent leakage that could turn the MOSFET on. Only SOURCE and DRAIN traces are allowed to run beside GATE traces. Use no-clean flux to minimize PCB contamination.

Note that the integrated boost regulator causes switched currents to flow in \( C_{AUX} \) and \( C_{OUT} \) and in the pins AUX, AUXSW, and GND. The loops formed by \( C_{AUX} \) and \( C_{OUT} \) should be minimized by placing these capacitors as close as possible to the LT8672 as shown in Figure 16 and Figure 17. \( C_{OUT} \) can be split into two capacitors \( C_{OUT1} \) (close to the LT8672) and \( C_{OUT2} \) (further away), provided that \( C_{OUT1} \) has a capacitance of at least 1 µF.
Figure 17. Recommended PCB Layout for the LT8672 (DFN)
TYPICAL APPLICATIONS

Active Rectifier for 12V Automotive Applications

Active Rectifier for 12V Automotive Applications with EMI Filter at DRAIN

Active Rectifier for 12V Automotive Applications with High Load
PACKAGE DESCRIPTION

MS Package
10-Lead Plastic MSOP

(Reference LTC DWG # 05-08-1661 Rev F)

NOTE:
1. DIMENSIONS IN MILLIMETER/(INCH)
2. DRAWING NOT TO SCALE
3. DIMENSION DOES NOT INCLUDE MOLD FLASH, PROTRUSIONS OR GATE BURRS.
   MOLD FLASH, PROTRUSIONS OR GATE BURRS SHALL NOT EXCEED 0.152mm (.006") PER SIDE
4. DIMENSION DOES NOT INCLUDE INTERLEAD FLASH OR PROTRUSIONS.
   INTERLEAD FLASH OR PROTRUSIONS SHALL NOT EXCEED 0.152mm (.006") PER SIDE
5. LEAD COPLANARITY (BOTTOM OF LEADS AFTER FORMING) SHALL BE 0.102mm (.004") MAX
**PACKAGE DESCRIPTION**

**DDB Package**

10-Lead Plastic DFN (3mm × 2mm) COL

(Reference LTC DWG # 05-08-1531 Rev Ø)

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**NOTE:**

1. DRAWING CONFORMS TO VERSION (WECD-1) IN JEDEC PACKAGE OUTLINE M0-229
2. DRAWING NOT TO SCALE
3. ALL DIMENSIONS ARE IN MILLIMETERS
4. DIMENSIONS OF EXPOSED PAD ON BOTTOM OF PACKAGE DO NOT INCLUDE MOLD FLASH. MOLD FLASH, IF PRESENT, SHALL NOT EXCEED 0.15mm ON ANY SIDE
5. EXPOSED PAD SHALL BE SOLDER PLATED
6. SHADED AREA IS ONLY A REFERENCE FOR PIN 1 LOCATION ON THE TOP AND BOTTOM OF PACKAGE
## REVISION HISTORY

<table>
<thead>
<tr>
<th>REV</th>
<th>DATE</th>
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</table>
| A   | 04/18| Added DFN package option  
Clarified Figure 16 and Figure 17  
Added Figure 17  
Added DFN package drawing | 1, 2, 6, 16, 17, 20 |
| B   | 09/18| Clarified Gate Turn-On and Turn-Off Delay Time | 3 |
| C   | 02/19| Added J-Grade temperature option  
Clarified $\theta_{JC}$ | 2, 3, 2 |
**TYPICAL APPLICATION**

Active Rectifier for 12V Automotive Applications with EMI Filter at SOURCE

**RELATED PARTS**

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<thead>
<tr>
<th>PART NUMBER</th>
<th>DESCRIPTION</th>
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<tr>
<td>LT3667/LT3668</td>
<td>40V (60V_{MAX}), 400mA Step-Down Switching Regulator with Dual Fault Protected LDOs</td>
<td>4.3V_{IN(MIN)}, 40V_{IN(MAX)} (60V_{MAX}), 0.8V_{OUT(MIN)}, I_{Q} = 50µA, I_{SD} = &lt;1µA, MSOP-16E and 3mm × 5mm QFN-24 Packages</td>
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<tr>
<td>LTC4359</td>
<td>Ideal Diode Controller with Reverse Input Protection</td>
<td>4V_{IN(MIN)}, 80V_{IN(MAX)}, -40V_{OUT(MIN)} Reverse Protection, I_{Q} = 150µA, I_{SD} = &lt;9µA, MSOP-8 and 2mm × 3mm DFN-6 Packages</td>
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<tr>
<td>LT8609S</td>
<td>42V, 2A, 94% Efficiency, 2.2MHz Synchronous Micropower Step-Down DC/DC Converter with I_{Q} = 2.5µA</td>
<td>3V_{IN(MIN)}, 42V_{IN(MAX)}, 0.8V_{OUT(MIN)}, I_{Q} = 2.5µA, I_{SD} = &lt;1µA, 3mm × 3mm LFQFN-16 Package</td>
</tr>
<tr>
<td>LT8650S</td>
<td>42V, Dual 4A, 95% Efficiency, 2.2MHz Synchronous Silent Switcher 2 Step-Down DC/DC Converter with I_{Q} = 6.2µA</td>
<td>3V_{IN(MIN)}, 42V_{IN(MAX)}, 0.8V_{OUT(MIN)}, I_{Q} = 6.2µA, I_{SD} = &lt;1µA, 4mm × 6mm LFQFN-32 Package</td>
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<tr>
<td>LT8640S</td>
<td>42V, 6A, 95% Efficiency, 2.2MHz Synchronous Silent Switcher2 Step-Down DC/DC Converter with I_{Q} = 2.5µA</td>
<td>3.4V_{IN(MIN)}, 42V_{IN(MAX)}, 0.97V_{OUT(MIN)}, I_{Q} = 2.5µA, I_{SD} = &lt;1µA, 4mm × 4mm LFQFN-24 Package</td>
</tr>
<tr>
<td>LT8645S</td>
<td>65V, 8A, 95% Efficiency, 2.2MHz Synchronous Silent Switcher 2 Step-Down DC/DC Converter with I_{Q} = 2.5µA</td>
<td>3.4V_{IN(MIN)}, 65V_{IN(MAX)}, 0.8V_{OUT(MIN)}, I_{Q} = 2.5µA, I_{SD} = &lt;1µA, 4mm × 6mm LFQFN-32 Package</td>
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<tr>
<td>LT8609/LT8609A/ LT8609B</td>
<td>42V, 2A, 94% Efficiency, 2.2MHz Synchronous Micropower Step-Down DC/DC Converter with I_{Q} = 2.5µA</td>
<td>3V_{IN(MIN)}, 42V_{IN(MAX)}, 0.8V_{OUT(MIN)}, I_{Q} = 2.5µA, I_{SD} = &lt;1µA, MSOP-10E Package</td>
</tr>
<tr>
<td>LT8640</td>
<td>42V, 5A, 95% Efficiency, 2.2MHz Synchronous Silent Switcher 2 Step-Down DC/DC Converter with I_{Q} = 2.5µA</td>
<td>3.4V_{IN(MIN)}, 42V_{IN(MAX)}, 0.97V_{OUT(MIN)}, I_{Q} = 2.5µA, I_{SD} = &lt;1µA, 3mm × 4mm QFN-16 Package</td>
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<tr>
<td>LT8612</td>
<td>42V, 6A, 96% Efficiency, 2.2MHz Synchronous Micropower Step-Down DC/DC Converter with I_{Q} = 2.5µA</td>
<td>3.4V_{IN(MIN)}, 42V_{IN(MAX)}, 0.97V_{OUT(MIN)}, I_{Q} = 3.0µA, I_{SD} = &lt;1µA, 3mm × 6mm QFN-28 Package</td>
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<tr>
<td>LT8602</td>
<td>42V, Quad Output (2.5A + 1.5A + 1.5A + 1.5A) 95% Efficiency, 2.2MHz Synchronous Micropower Step-Down DC/DC Converter with I_{Q} = 25µA</td>
<td>3V_{IN(MIN)}, 42V_{IN(MAX)}, 0.8V_{OUT(MIN)}, I_{Q} = 25µA, I_{SD} = &lt;1µA, 6mm × 6mm QFN-40 Package</td>
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