

# Sine-wave Driving, High Voltage 3-phase Motor Drivers with Built-in Hall Amplifiers SIM260xM Series

## Description

The SIM260xM series are high voltage 3-phase motor drivers driven by a sinusoidal control, which can support Hall element and Hall IC inputs, thus offering high-efficient yet low-noise motor control. Supplied in a highly heat-dissipating DIP package, where a controller, a gate driver, the output transistors of three phases, and bootstrap diodes are highly integrated, the SIM260xM series requires only a few external components for building a motor driver. This also allows a motor driver to be highly reliable in performance and design-friendly with its compactness. These products can optimally control the inverter systems of low- to medium-capacity motors that require universal input standards.

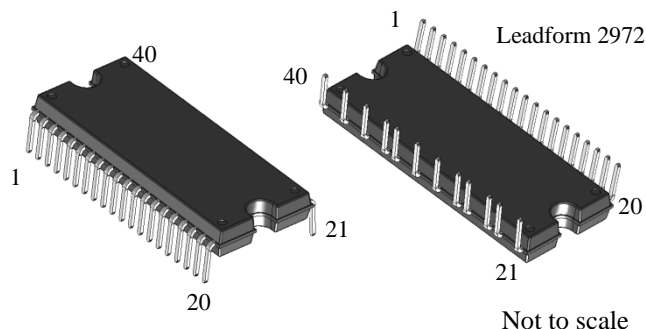
## Features

- Pb-free (RoHS Compliant)
- SIM2601MA:  
Isolation Voltage: 1500 V (for 1 min)  
(UL Recognition Pending)
- SIM2602M:  
Isolation Voltage: 1500 V (for 1 min)  
UL-recognized Component (File No.: E118037)
- Low Noise, High Efficiency  
(Sinusoidal Current Waveform)
- Reduced Number of Parts Achieved by Built-in Bootstrap Diodes
- Hall Element and Hall IC Inputs
- Application-specific Optimal Settings with External Signals:
  - Motor Speed
  - Phase Advance Angle
  - Motor Direction
  - User-settable Motor Lock Detection (Enabled or Disabled)
- 5 V Reference Voltage Output  
(Used for Driving Hall Elements etc.)
- Fault Signal Output at Protection Activation (FO Pin)
- Protections Include:
  - VREG Pin Undervoltage Lockout (UVLO\_REG)
  - Undervoltage Lockout for Power Supplies  
VBx Pin (UVLO\_VB)  
VCC Pin (UVLO\_VCC)
  - Overcurrent Limit (OCL)
  - Overcurrent Protection (OCP)
  - Thermal Shutdown (TSD)
  - Motor Lock Protection (MLP)
  - Reverse Rotation Detection
  - Hall Signal Abnormality Detection

## Package

DIP40

Mold Dimensions: 36.0 mm × 14.8 mm × 4.0 mm



## Selection Guide

- Breakdown Voltage: 600 V

I <sub>O</sub>	Part Number	Output Transistor
2.5 A	SIM2601MA*	Power MOSFET
5.0 A	SIM2602M	IGBT + FRD

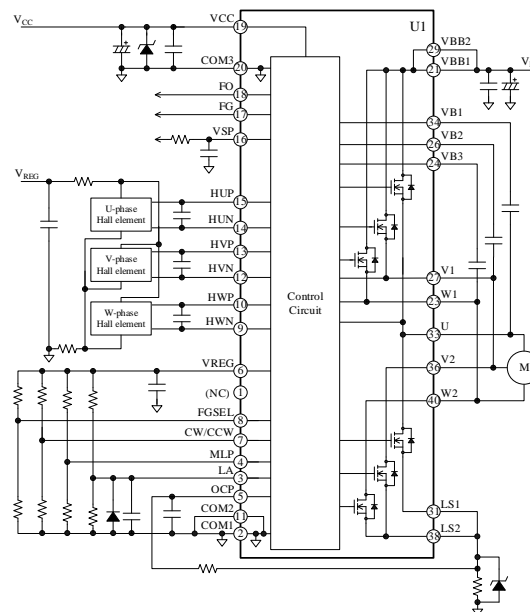
\* Under development

## Applications

For motor drives such as:

- Fan Motor and Pump Motor for Washer and Dryer
- Fan Motor for Air Conditioner
- Fan Motor for Air Purifier and Electric Fan

## Typical Application



## Contents

Description .....	1
Contents .....	2
1. Absolute Maximum Ratings .....	4
2. Recommended Operating Conditions .....	5
3. Electrical Characteristics .....	6
3.1 Characteristics of Control Parts .....	6
3.2 Bootstrap Diode Characteristics .....	7
3.3 Transistor Characteristics .....	8
3.3.1 SIM2601MA .....	8
3.3.2 SIM2602M .....	9
3.4 Thermal Resistance Characteristics .....	10
4. Mechanical Characteristics .....	11
5. Insulation Distance .....	11
6. Block Diagrams .....	12
7. Pin Configuration Definitions .....	13
8. Typical Applications .....	14
9. Physical Dimensions .....	16
10. Marking Diagram .....	17
11. Functional Descriptions .....	18
11.1 Pin Descriptions .....	18
11.1.1 COM1, COM2, and COM3 .....	18
11.1.2 LA .....	18
11.1.3 MLP .....	18
11.1.4 OCP .....	18
11.1.5 VREG .....	18
11.1.6 CW/CCW .....	19
11.1.7 FGSEL .....	19
11.1.8 HUP, HVP, and HWN; HUN, HVN, and HWP .....	19
11.1.9 VSP .....	19
11.1.10 FG .....	19
11.1.11 FO .....	20
11.1.12 VCC .....	20
11.1.13 VBB1 and VBB2 .....	20
11.1.14 VB1, VB2, and VB3 .....	20
11.1.15 U, V1, V2, W1, and W2 .....	20
11.1.16 LS1 and LS2 .....	20
11.2 Startup Operation .....	21
11.3 Charging of Bootstrap Capacitors .....	21
11.4 Motor Speed Control .....	22
11.5 Phase Advance Function .....	22
11.6 Fault Signal Output .....	27
11.7 Protection Functions .....	27
11.7.1 VREG Pin Undervoltage Lockout (UVLO_VREG) .....	27
11.7.2 Undervoltage Lockout for Power Supply (UVLO) .....	27
11.7.3 Overcurrent Limit (OCL) and Overcurrent Protection (OCP) .....	27
11.7.4 Thermal Shutdown (TSD) .....	28
11.7.5 Motor Lock Protection (MLP) .....	28
11.7.6 Reverse Rotation Detection .....	28
11.7.7 Hall Signal Abnormality Detection .....	28
12. Design Notes .....	30

12.1	PCB Pattern Layout	30
12.2	Considerations in IC Characteristics Measurement	30
12.3	Considerations in Heatsink Mounting	31
13.	Calculating Power Losses and Estimating Junction Temperature	31
13.1	Power MOSFET	31
13.1.1	Power MOSFET Steady-state Loss, $P_{RON}$	31
13.1.2	Power MOSFET Switching Loss, $P_{SW}$	32
13.1.3	Body Diode Steady-state Loss, $P_{SD}$	32
13.1.4	Estimating Junction Temperature of Power MOSFET	32
13.2	IGBT	33
13.2.1	IGBT Steady-state Loss, $P_{ON}$	33
13.2.2	IGBT Switching Loss, $P_{SW}$	33
13.2.3	Estimating Junction Temperature of IGBT	33
14.	Performance Curves	34
14.1	Transient Thermal Resistance Curves	34
14.2	Performance Curves of Control Parts	35
14.3	Performance Curves of Output Parts	39
14.3.1	Transistor Characteristics	39
14.3.2	Switching Losses	40
14.4	Allowable Effective Current Curves	41
14.4.1	SIM2601MA	41
14.4.2	SIM2602M	41
14.5	Short Circuit SOA (Safe Operating Area)	42
15.	Pattern Layout Example	43
16.	Typical Motor Driver Application	45
	Important Notes	46

## SIM260xM Series

### 1. Absolute Maximum Ratings

Current polarities are defined as follows: current going into the IC (sinking) is positive current (+); current coming out of the IC (sourcing) is negative current (-).

Unless specifically noted,  $T_A = 25\text{ }^{\circ}\text{C}$ , COM1 = COM2 = COM3 = COM.

Parameter	Symbol	Conditions	Rating	Unit	Remarks
Main Supply Voltage (DC) <sup>(1)</sup>	$V_{DC}$	VBBx-LSx	450	V	SIM2602M
Main Supply Voltage (Surge) <sup>(1)</sup>	$V_{DC(SURGE)}$	VBBx-LSx	500	V	SIM2602M
Power MOSFET / IGBT Breakdown Voltage	$V_{DSS}$	$I_D = 100\text{ }\mu\text{A}$	600	V	SIM2601MA
	$V_{CES}$	$I_C = 1\text{ mA}$	600	V	SIM2602M
Logic Supply Voltage	$V_{CC}$	VCC-COM	20	V	
	$V_{BS}$	VB1-U, VB2-V1, VB3-W1	20	V	
Output Current (DC) <sup>(2)</sup>	$I_O$	$T_C = 25\text{ }^{\circ}\text{C}$ , $T_J < 150\text{ }^{\circ}\text{C}$	2.5	A	SIM2601MA
			5.0		SIM2602M
Output Current (Pulse)	$I_{OP}$	$T_C = 25\text{ }^{\circ}\text{C}$ , pulse width $\leq 100\text{ }\mu\text{s}$	3.75	A	SIM2601MA
			7.5		SIM2602M
VREG Pin Output Voltage	$V_{REG}$		5.5	V	
VREG Pin Current	$I_{REG}$		30	mA	
Input Voltage 1 (HUP, HUN, HVP, HVN, HWP, HWN)	$V_{IN(1)}$		-0.5 to $V_{REG}$	V	
Input Voltage 2 (LA, MLP, OCP, CW/CCW, FGSEL)	$V_{IN(2)}$		-0.5 to $V_{REG}$	V	
Input Voltage 3 (VSP)	$V_{IN(3)}$		-0.5 to 10	V	
Output Voltage (FG, FO)	$V_O$		-0.5 ~ $V_{REG}$	V	
LSx Pin Voltage (DC)	$V_{LS(DC)}$	LSx-COM	-0.7 to 7	V	
LSx Pin Voltage (Surge)	$V_{LS(SURGE)}$	LSx-COM	-4 to 7	V	
Operating Case Temperature <sup>(3)</sup>	$T_{C(OP)}$		-30 to 100	$^{\circ}\text{C}$	
Junction Temperature <sup>(4)</sup>	$T_J$		150	$^{\circ}\text{C}$	
Storage Temperature	$T_{STG}$		-40 to 150	$^{\circ}\text{C}$	

<sup>(1)</sup> Defined for the IGBT-embedded device only.

<sup>(2)</sup> Should be derated depending on an actual case temperature. See Section 14.4.

<sup>(3)</sup> Refers to a case temperature measured during IC operation.

<sup>(4)</sup> Refers to the junction temperature of each chip built in the IC, including the control stage, gate drive stage, and output transistors.

## SIM260xM Series

### 2. Recommended Operating Conditions

Unless specifically noted, COM1 = COM2 = COM3 = COM.

Parameter	Symbol	Conditions	Min.	Typ.	Max.	Unit	Remarks
Main Supply Voltage	$V_{DC}$	VBBx-LSx	—	300	400	V	
Logic Supply Voltage	$V_{CC}$	VCC-COM	13.5	—	16.5	V	
	$V_{BS}$	VB1-U, VB2-V, VB3-W1	13.5	—	16.5	V	
Input Voltage 1 (HUP, HUN, HVP, HVN, HWP, HWN)	$V_{IN(1)}$		0	—	5.0	V	
Input Voltage 2 (MLP, CW/CCW, FGSEL)	$V_{IN(2)}$		0	—	5.0		
Input Voltage 3 (VSP)	$V_{IN(3)}$		0	—	5.4	V	
FO Pin Noise Filter Capacitor	$C_{FO}$		0.001	—	0.01	$\mu\text{F}$	
Bootstrap Capacitor	$C_B$		1	—	—	$\mu\text{F}$	
Shunt Resistor*	$R_S$	$I_{OP} \leq 3.75 \text{ A}$	176	—	—	m $\Omega$	SIM2601MA
		$I_{OP} \leq 7.5 \text{ A}$	88	—	—		SIM2602M
RC Filter Resistor	$R_O$		—	—	100	$\Omega$	
RC Filter Capacitor	$C_O$		100	—	2200	pF	
Operating Case Temperature	$T_{C(OP)}$		—	—	100	$^{\circ}\text{C}$	

\* Should be a low-inductance resistor.

### 3. Electrical Characteristics

Current polarities are defined as follows: current going into the IC (sinking) is positive current (+); current coming out of the IC (sourcing) is negative current (-).

Unless specifically noted,  $T_A = 25\text{ }^{\circ}\text{C}$ ,  $V_{CC} = 15\text{ V}$ ,  $\text{COM1} = \text{COM2} = \text{COM3} = \text{COM}$ .

#### 3.1 Characteristics of Control Parts

Parameter	Symbol	Conditions	Min.	Typ.	Max.	Unit
<b>Power Supply Operation</b>						
Low-side Logic Operation Start Voltage	$V_{CC(ON)}$	VCC-COM	10.5	11.5	12.5	V
Low-side Logic Operation Stop Voltage	$V_{CC(OFF)}$		10.0	11.0	12.0	V
High-side Logic Operation Start Voltage	$V_{BS(ON)}$	VB1-U, VB2-V1, VB3-W1	9.5	10.5	11.5	V
High-side Logic Operation Stop Voltage	$V_{BS(OFF)}$		9.0	10.0	11.0	V
Logic Supply Current	$I_{CC}$	$V_{SP} = 5.4\text{ V}$ , $I_{REG} = 0\text{ A}$	—	5.5	—	mA
	$I_{BS}$	$V_{Bx} = 15\text{ V}$ , $V_{SP} = 5.4\text{ V}$ ; VBx pin current in 1-phase operation	40	140	350	$\mu\text{A}$
VREG Pin Output Voltage	$V_{REG}$	$I_{REG} = 0\text{ mA}$ to $30\text{ mA}$	4.5	5.0	5.5	V
<b>Input Signal<sup>(1)</sup></b>						
Input Threshold Voltage (MLP, FGSEL, CW/CCW)	$V_{TH}$		2.25	2.50	2.75	V
High Level Input Current 1 (LA, MLP, CW/CCW, FGSEL, VSP)	$I_{IH1}$	$V_{IN} = V_{REG}$	—	25	100	$\mu\text{A}$
Low Level Input Current 1 (LA, MLP, CW/CCW, FGSEL, VSP)	$I_{IL1}$	$V_{INL} = 0\text{ V}$	—	—	2	$\mu\text{A}$
High Level Input Current 2 (OCP)	$I_{IH2}$	$V_{IN} = V_{REG}$	-5	—	5	$\mu\text{A}$
Low Level Input Current 2 (OCP)	$I_{IL2}$	$V_{INL} = 0\text{ V}$	—	23	90	$\mu\text{A}$
High Level Input Current 3 (HUP, HUN, HVP, HVN, HWP, HWN)	$I_{IH3}$	$V_{IN} = V_{REG}$	-5	—	5	$\mu\text{A}$
Low Level Input Current 3 (HUP, HUN, HVP, HVN, HWP, HWN)	$I_{IL3}$	$V_{INL} = 0\text{ V}$	-5	—	5	$\mu\text{A}$
High Level Output Voltage (FG, FO)	$V_{OH}$		4.5	—	5.5	V
Low Level Output Voltage (FG, FO)	$V_{OL}$		—	—	0.5	V

<sup>(1)</sup> Guaranteed by design.

## SIM260xM Series

Parameter	Symbol	Conditions	Min.	Typ.	Max.	Unit
PWM Control						
PWM Carrier Frequency <sup>(2)</sup>	f <sub>C</sub>		16	17	18	kHz
Internal Oscillator Frequency <sup>(2)</sup>	f <sub>OSC</sub>		4.10	4.32	4.54	MHz
Dead Time <sup>(2)</sup>	t <sub>D</sub>		—	1.2	—	μs
Control IC Output Pulse Duty Cycle (Low-side) <sup>(2)</sup>	D	V <sub>SP</sub> = 1.5 V; with bootstrap capacitors being charged	—	6.3	—	%
Control IC Output Pulse Duty Cycle (High-side) <sup>(2)</sup>	D	V <sub>SP</sub> = 2.0 V	—	0	3	%
		V <sub>SP</sub> = 3.7 V	47	50	53	%
		V <sub>SP</sub> = 5.0 V (driven by trapezoidal control)	85.0	—	88.9	%
		V <sub>SP</sub> = 5.4 V (driven by sinusoidal control)	93.7	—	100	%
Protection						
OCL Threshold Voltage	V <sub>LIM</sub>		0.25	0.30	0.35	V
OCL Blanking Time	t <sub>BK(OCL)</sub>		—	2.3	4.5	μs
OCP Threshold Voltage	V <sub>TRIP</sub>		0.54	0.60	0.66	V
OCP Blanking Time	t <sub>BK(OCP)</sub>		—	0.8	1.7	μs
OCP Hold Time	t <sub>P</sub>		—	15	—	ms
MLP Detection Time	t <sub>LD</sub>		—	5	—	s
MLP Hold Time	t <sub>LH</sub>		—	64	—	s
TSD Operating Temperature <sup>(3)</sup>	T <sub>DH</sub>	I <sub>REG</sub> = 0 mA; without heatsink	—	130	—	°C
TSD Hysteresis Temperature <sup>(3)</sup>	T <sub>D(HYS)</sub>		—	30	—	°C
VREG Pin Undervoltage Lockout Operating Voltage <sup>(2)</sup>	V <sub>UVRL</sub>		3.24	3.60	3.96	V
VREG Pin Undervoltage Lockout Releasing Voltage <sup>(2)</sup>	V <sub>UVRH</sub>		3.60	4.00	4.40	V

<sup>(2)</sup> Refers to an internal signal; guaranteed by design.

<sup>(3)</sup> Refers to the junction temperature of the gate drive stage.

### 3.2 Bootstrap Diode Characteristics

Parameter	Symbol	Conditions	Min.	Typ.	Max.	Unit
Bootstrap Diode Leakage Current	$I_{LBD}$	$V_R = 600 \text{ V}$	—	—	100	$\mu A$
Bootstrap Diode Forward Voltage	$V_{FB}$	$I_{FB} = 10 \text{ mA}$ ; voltage drop in $R_{BOOT}$ included	—	3.0	—	V

### 3.3 Transistor Characteristics

Figure 3-1 provides the definitions of switching characteristics described in this and the following sections. Internal signals, HINx and LINx, are defined as  $V_{IN}$  (see Section 6).

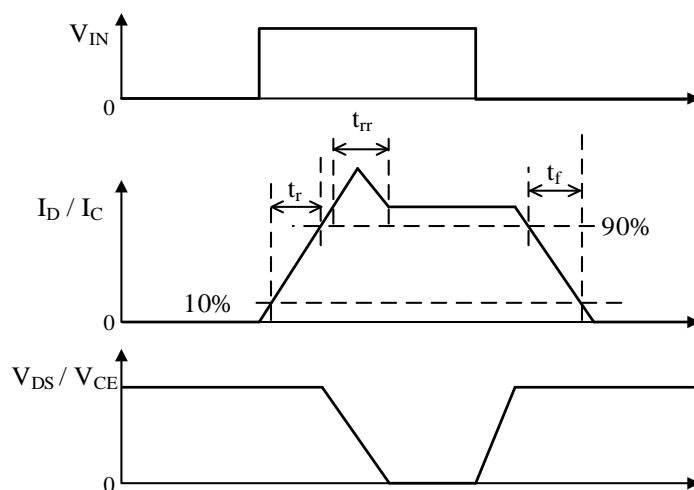


Figure 3-1. Switching Characteristics Definitions

#### 3.3.1 SIM2601MA

Parameter	Symbol	Conditions	Min.	Typ.	Max.	Unit
Drain-to-Source Leakage Current	I <sub>DSS</sub>	V <sub>DS</sub> = 600 V, V <sub>IN</sub> = 0 V	—	—	100	μA
Drain-to-Source On-resistance	R <sub>DS(ON)</sub>	I <sub>D</sub> = 1.25 A, V <sub>IN</sub> = 5 V	—	2.0	2.5	Ω
Source-to-Drain Diode Forward Voltage	V <sub>SD</sub>	I <sub>SD</sub> = 1.25 A, V <sub>IN</sub> = 0 V	—	1.0	1.5	V
High-side Switching						
Source-to-Drain Diode Reverse Recovery Time*	t <sub>rr</sub>	V <sub>DC</sub> = 300 V, I <sub>D</sub> = 1.25 A,	—	100	—	ns
Rise Time*	t <sub>r</sub>	V <sub>IN</sub> = 0→5 V or 5→0 V, T <sub>J</sub> = 25 °C,	—	50	—	ns
Fall Time*	t <sub>f</sub>	inductive load	—	35	—	ns
Low-side Switching						
Source-to-Drain Diode Reverse Recovery Time*	t <sub>rr</sub>	V <sub>DC</sub> = 300 V, I <sub>D</sub> = 1.25 A,	—	100	—	ns
Rise Time*	t <sub>r</sub>	V <sub>IN</sub> = 0→5 V or 5→0 V, T <sub>J</sub> = 25 °C,	—	55	—	ns
Fall Time*	t <sub>f</sub>	inductive load	—	20	—	ns

\* Guaranteed by design.



## SIM260xM Series

### 3.3.2 SIM2602M

Parameter	Symbol	Conditions	Min.	Typ.	Max.	Unit
Collector-to-Emitter Leakage Current	I <sub>CES</sub>	V <sub>CE</sub> = 600 V, V <sub>IN</sub> = 0 V	—	—	1	mA
Collector-to-Emitter Saturation Voltage	V <sub>CE(SAT)</sub>	I <sub>C</sub> = 5.0 A, V <sub>IN</sub> = 5 V	—	1.75	2.2	V
Diode Forward Voltage	V <sub>F</sub>	I <sub>F</sub> = 5.0 A, V <sub>IN</sub> = 0 V	—	2.0	2.4	V
High-side Switching						
Source-to-Drain Diode Reverse Recovery Time*	t <sub>rr</sub>	V <sub>DC</sub> = 300 V, I <sub>C</sub> = 5.0 A, V <sub>IN</sub> = 0→5 V or 5→0 V, T <sub>J</sub> = 25 °C, inductive load	—	100	—	ns
Rise Time*	t <sub>r</sub>		—	110	—	ns
Fall Time*	t <sub>f</sub>		—	210	—	ns
Low-side Switching						
Source-to-Drain Diode Reverse Recovery Time*	t <sub>rr</sub>	V <sub>DC</sub> = 300 V, I <sub>C</sub> = 5.0 A, V <sub>IN</sub> = 0→5 V or 5→0 V, T <sub>J</sub> = 25 °C, inductive load	—	100	—	ns
Rise Time*	t <sub>r</sub>		—	110	—	ns
Fall Time*	t <sub>f</sub>		—	210	—	ns

\* Guaranteed by design.

### 3.4 Thermal Resistance Characteristics

Parameter	Symbol	Conditions	Min.	Typ.	Max.	Unit	Remarks
Junction-to-Case Thermal Resistance <sup>(1)</sup>	$R_{J-C}$	All power MOSFETs operating	—	—	3.6	°C/W	SIM2601MA
	$R_{(J-C)Q}^{(2)}$	All IGBTs operating	—	—	3.6	°C/W	SIM2602M
	$R_{(J-C)F}^{(3)}$	All freewheeling diodes operating	—	—	4.2	°C/W	SIM2602M
Junction-to-Ambient Thermal Resistance	$R_{J-A}$	All power MOSFETs operating	—	—	25	°C/W	SIM2601MA
	$R_{(J-A)Q}$	All IGBTs operating	—	—	25	°C/W	SIM2602M
	$R_{(J-A)F}$	All freewheeling diodes operating	—	—	29	°C/W	SIM2602M

<sup>(1)</sup> Refers to a case temperature at the measurement point described in Figure 3-2.

<sup>(2)</sup> Refers to steady-state thermal resistance between the junction of the built-in transistors and the case. For transient thermal characteristics, see Section 14.1.

<sup>(3)</sup> Refers to steady-state thermal resistance between the junction of the built-in freewheeling diodes and the case.

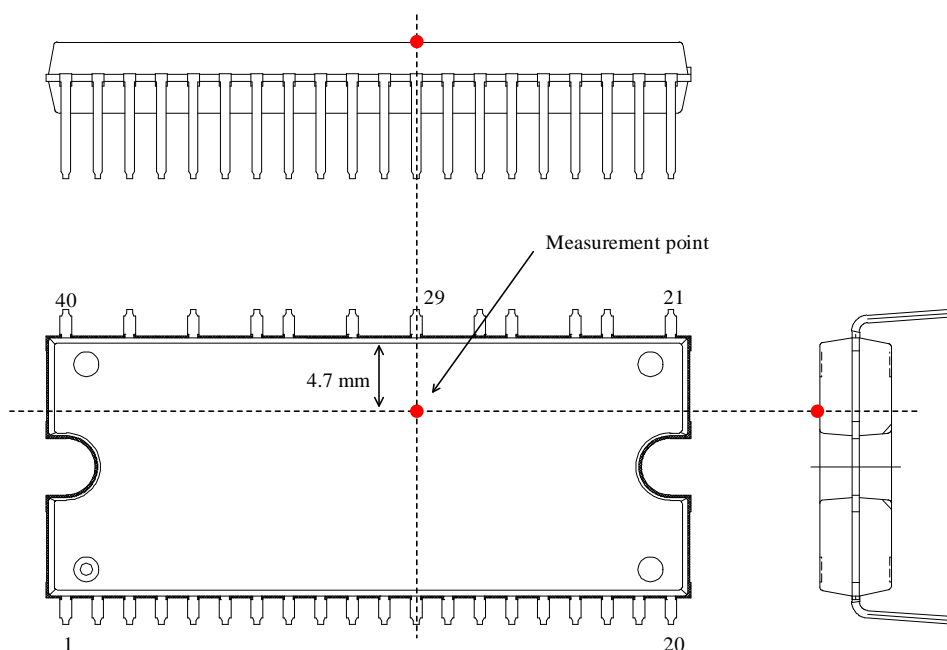


Figure 3-2. Case Temperature Measurement Point

#### 4. Mechanical Characteristics

Parameter	Conditions	Min.	Typ.	Max.	Unit	Remarks
Heatsink Mounting Screw Torque	*	0.294	—	0.441	N·m	
Flatness of Heatsink Attachment Area	See Figure 4-1.	0	—	60	μm	
Package Weight		—	5.2	—	g	

\* Requires using a metric screw of M2.5 and a plain washer of 6.0 mm (φ). For more on screw tightening, see Section 12.3.

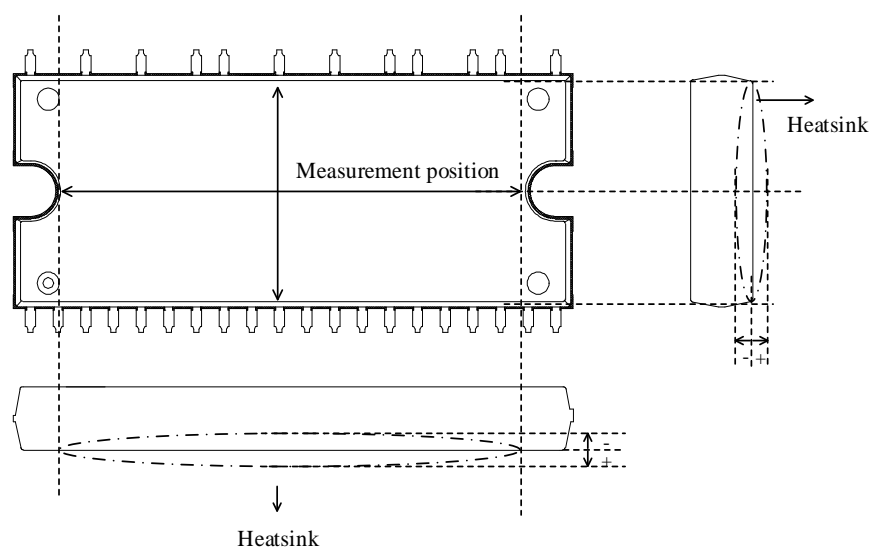


Figure 4-1. Flatness Measurement Position

#### 5. Insulation Distance

Parameter	Conditions	Min.	Typ.	Max.	Unit	Remarks
Clearance	Between heatsink* and leads. See Figure 5-1.	1.5	—	2.1	mm	
Creepage		1.7	—	—	mm	

\* Refers to when a heatsink to be mounted is flat. If your application requires a clearance exceeding the maximum distance given above, use an alternative (e.g., a convex heatsink) that will meet the target requirement.

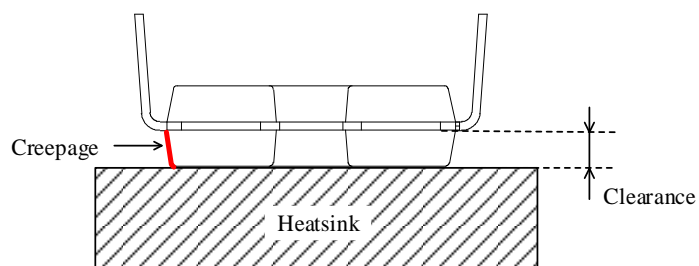


Figure 5-1. Insulation Distance Definitions

## 6. Block Diagrams

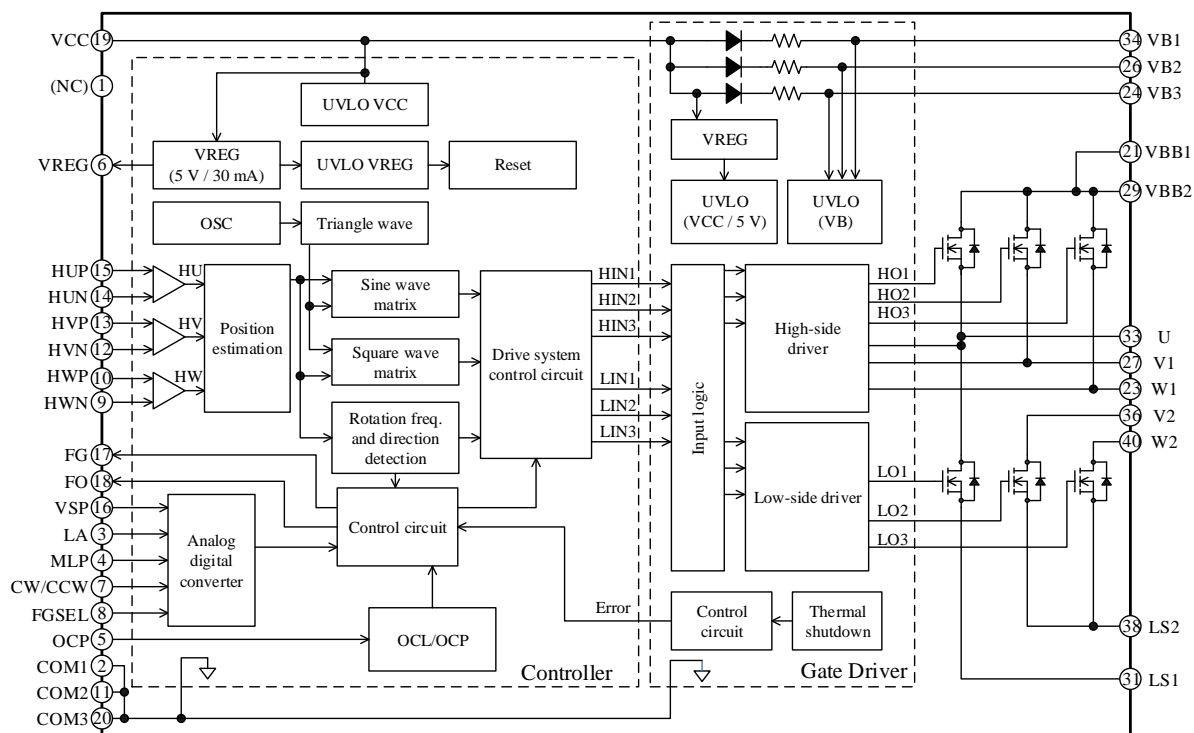


Figure 6-1. Block Diagram: SIM2601MA

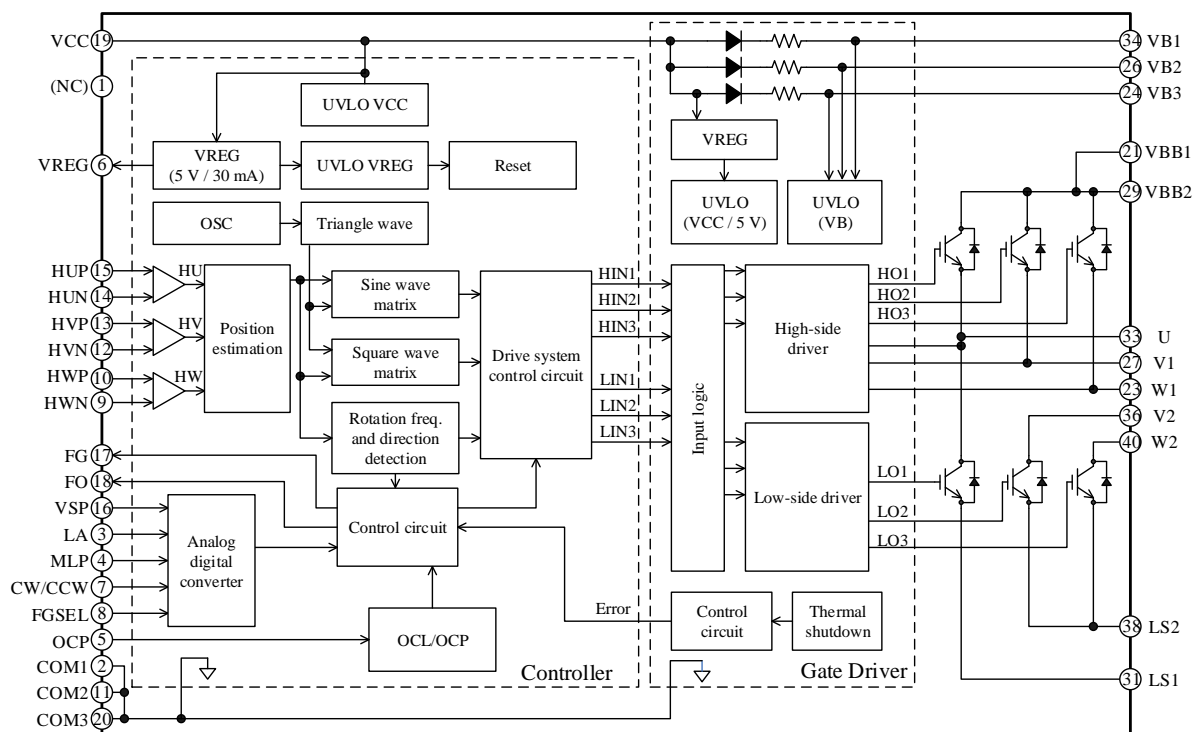


Figure 6-2. Block Diagram: SIM2602M

## 7. Pin Configuration Definitions

Top View				Pin Number	Pin Name	Description
1	(NC)	W2	40	1	NC	(No connection)
2	COM1		39	2	COM1	Logic ground
3	LA	LS2	38	3	LA	Input for phase advance angle setting signal
4	MLP		37	4	MLP	Setting pin to enable or disable the motor lock protection
5	OCF	V2	36	5	OCF	Input for overcurrent detection signal
6	VREG		35	6	VREG	Internal regulator output
7	CW/CCW	VB1	34	7	CW/CCW	Input for motor direction setting signal
8	FGSEL	U	33	8	FGSEL	Input for FG pin setting signal
9	HWN		32	9	HWN	W-phase Hall element negative signal input (-)
10	HWP	LS1	31	10	HWP	W-phase Hall element positive signal input (+)
11	COM2		30	11	COM2	Logic ground
12	HVN	VBB2	29	12	HVN	V-phase Hall element negative signal input (-)
13	HVP		28	13	HVP	V-phase Hall element positive signal input (+)
14	HUN	V1	27	14	HUN	U-phase Hall element negative signal input (-)
15	HUP	VB2	26	15	HUP	U-phase Hall element positive signal input (+)
16	VSP		25	16	VSP	Input for motor speed control signal
17	FG	VB3	24	17	FG	Rotation pulse signal output
18	FO	W1	23	18	FO	Fault signal output
19	VCC		22	19	VCC	Input for logic supply voltage
20	COM3	VBB1	21	20	COM3	Logic ground
				21	VBB1	Positive DC bus supply voltage (+)
				22	—	Pin removed
				23	W1	W-phase output (connected to W2 externally)
				24	VB3	W-phase high-side floating supply voltage input
				25	—	Pin removed
				26	VB2	V-phase high-side floating supply voltage input
				27	V1	V-phase output (connected to V2 externally)
				28	—	Pin removed
				29	VBB2	Positive DC bus supply voltage (+)
				30	—	Pin removed
				31	LS1	U-phase low-side power MOSFET source or IGBT emitter (connected to L2 externally)
				32	—	Pin removed
				33	U	U-phase output
				34	VB1	U-phase high-side floating supply voltage input
				35	—	Pin removed
				36	V2	V-phase output (connected to V1 externally)
				37	—	Pin removed
				38	LS2	V-/W- phases low-side power MOSFET source or IGBT emitter (connected to L1 externally)
				39	—	Pin removed
				40	W2	W-phase output (connected to W1 externally)



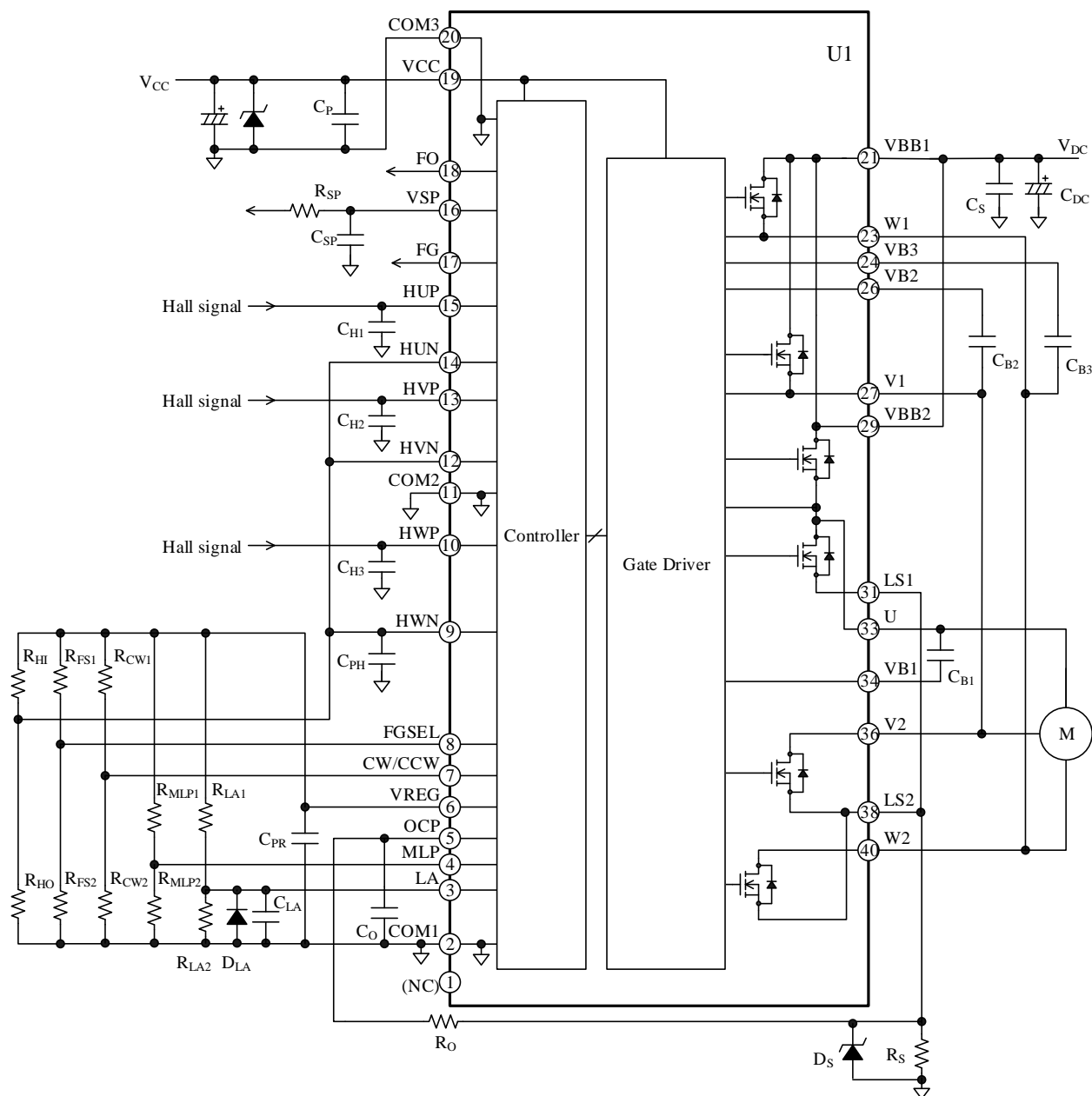
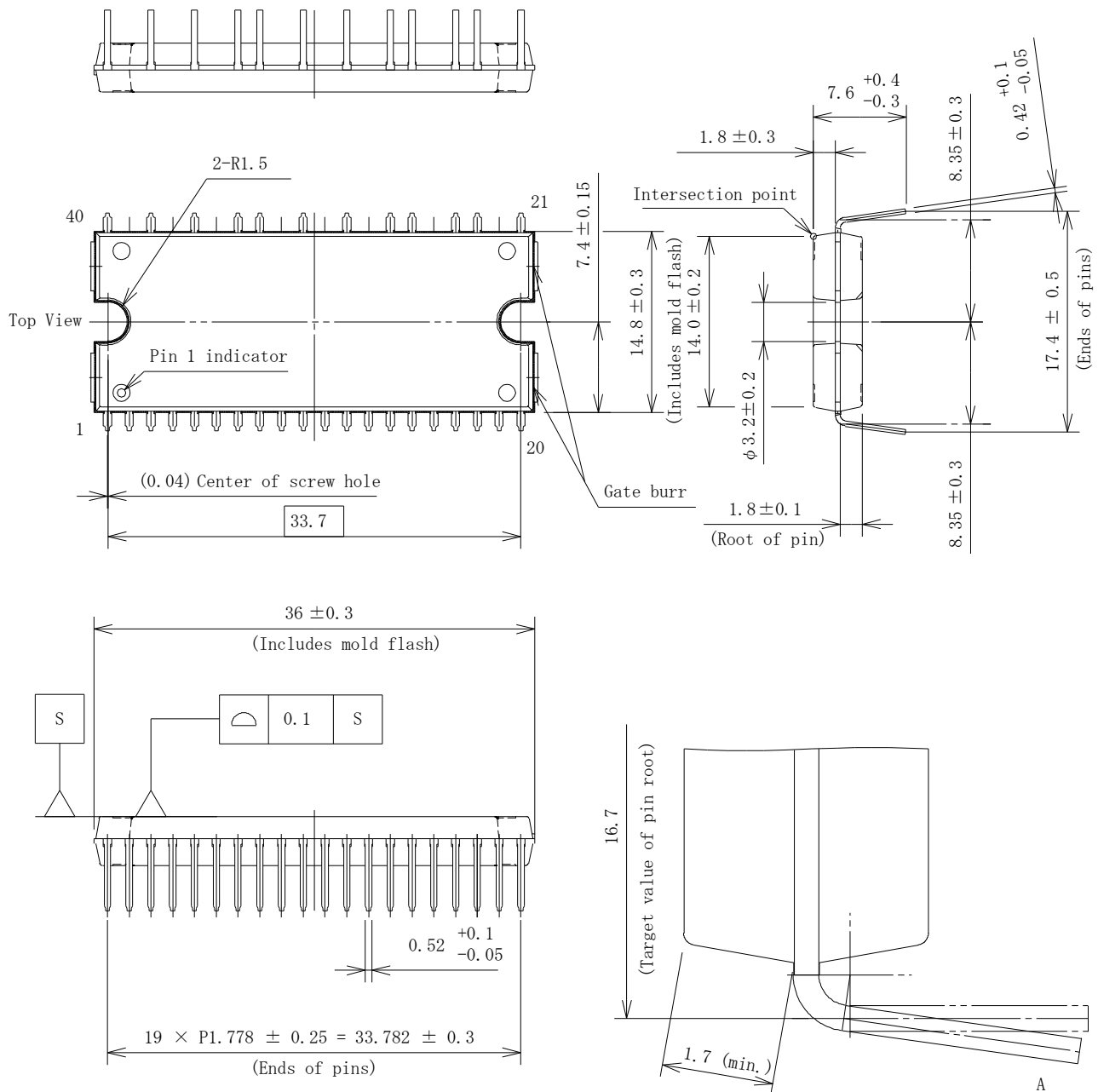


Figure 8-2. Application Using Signals Input from Hall ICs

## 9. Physical Dimensions

### • DIP40 Package



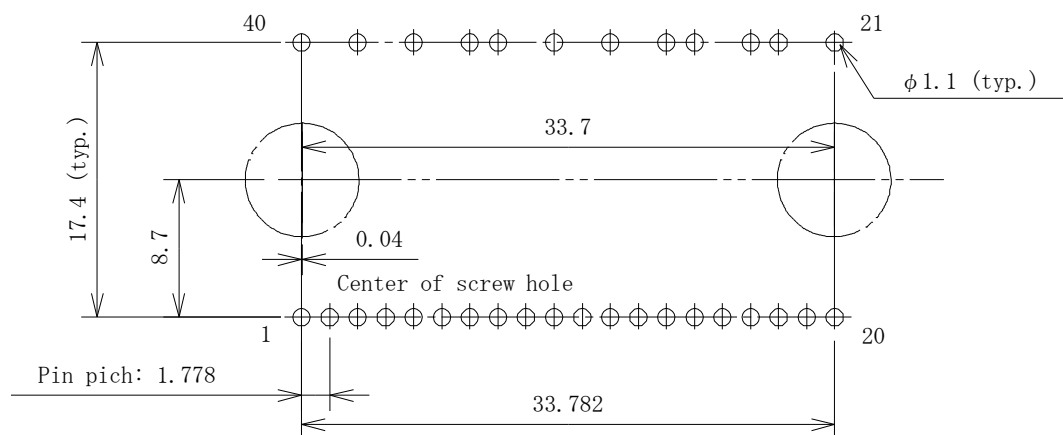
### NOTES:

- Dimensions in millimeters
- Pb-free (RoHS compliant)
- “A” represents a pin illustrated for reference only, not the actual state of a bend.
- Maximum gate burr height is 0.3 mm.



## SIM260xM Series

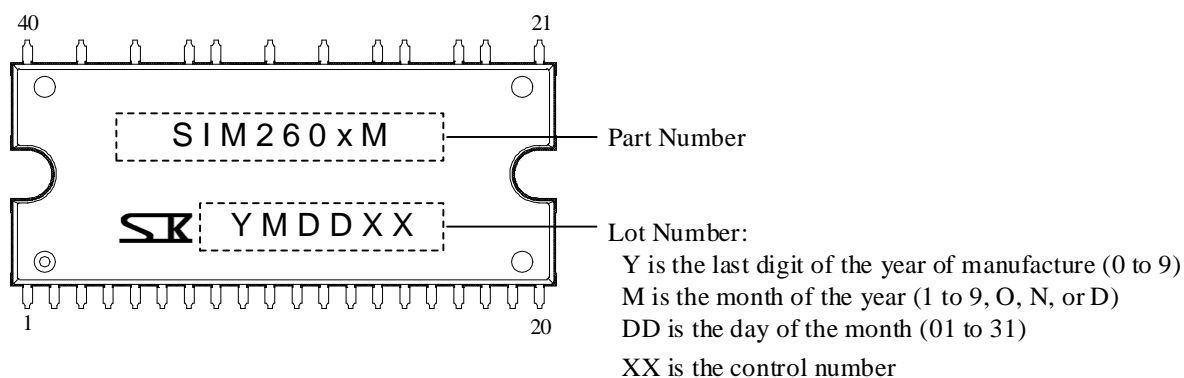
- Land Pattern Example
- Reference Through Hole Size and Layout



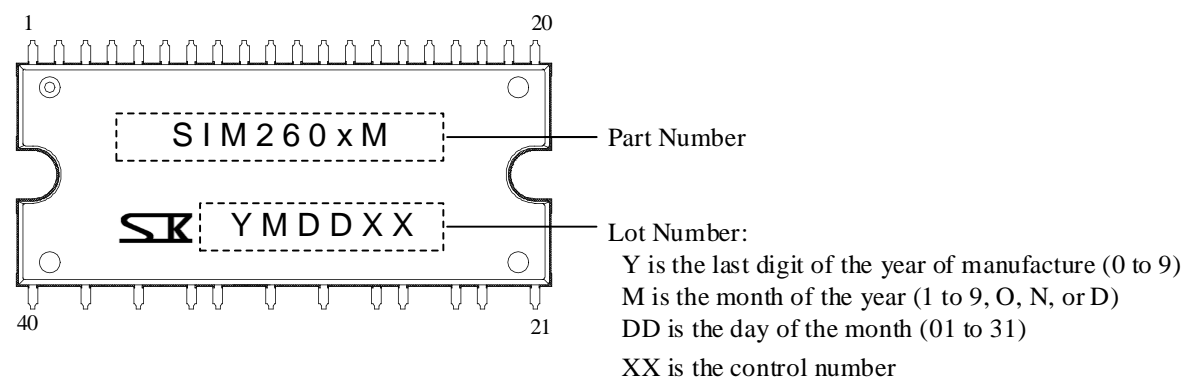
Unit: mm

## 10. Marking Diagram

- Front-side Marking



- Back-side Marking



## 11. Functional Descriptions

Unless specifically noted, this section uses the following definitions:

- For concise descriptions, this section employs notation systems that denote the electrical characteristics symbols listed in Section 3 and the electronic symbol names of the typical applications in Section 8. All the characteristic values given in this section are typical values, unless they are specified as minimum or maximum.
- All the circuit diagrams listed in this section represent the type of IC that incorporates power MOSFETs. All the functional descriptions in this section are also applicable to the type of IC that incorporates IGBTs.
- For pin and peripheral component descriptions, this section employs a notation system that denotes a pin name or an electronic symbol name with the arbitrary letter “x”, representing the certain numbers and letters (1 to 3 and U to W). Thus, “the VBx pin” is used when referring to any or all of the VB1, VB2, and VB3 pins.

### 11.1 Pin Descriptions

#### 11.1.1 COM1, COM2, and COM3

These are the logic ground pins for the built-in control ICs and are internally connected. Varying electric potential of the logic ground can be a cause of improper operations. Therefore, connect the logic ground as close and short as possible to a shunt resistor,  $R_S$ , at a single-point ground (or star ground) which is separated from the power ground (see Figure 11-1).

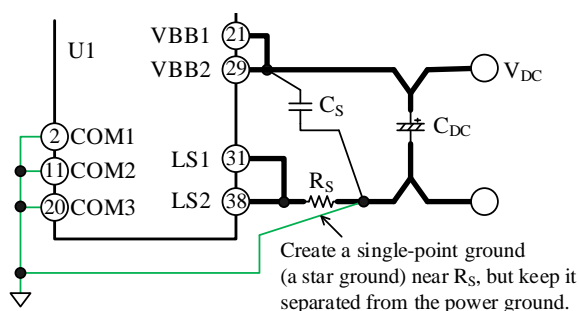


Figure 11-1. Connections to Logic Ground

#### 11.1.2 LA

The IC features the phase advance function. The angle of phase advance is determined by an analog voltage applied to the LA pin. Section 11.5 gives detailed explanations on the LA pin settings and the phase advance function.

#### 11.1.3 MLP

The IC determines to enable or disable the motor lock protection based on the setting of this pin. Table 11-1 provides the logic level definitions for the MLP pin. The IC detects which logic level the MLP pin has been set during a startup period (i.e., when the VCC pin voltage is rising). Figure 11-2 shows an internal circuit diagram of the MLP pin. To set the MLP pin to logic low, connect the pin to the GND pin. To set the MLP pin to logic high, connect the pin to the VREG pin. Section 11.7.5 explains more details on the motor lock protection.

Table 11-1. Logic Levels Defined for MLP Pin

MLP Pin	MLP Setting Status
L	Enabled
H	Disabled

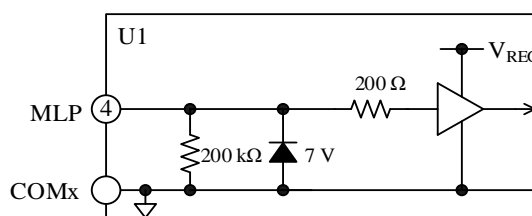


Figure 11-2. Internal Circuit Diagram of MLP Pin

#### 11.1.4 OCP

This pin serves as the input of the overcurrent protection (OCP) which monitors the currents flowing through the output transistors. The IC determines which of the overcurrent limit (OCL) and overcurrent protection (OCP) functions to activate according to the level of a voltage applied to the OCP pin. Section 11.7.3 provides further information about the OCP circuit configuration and its mechanism.

#### 11.1.5 VREG

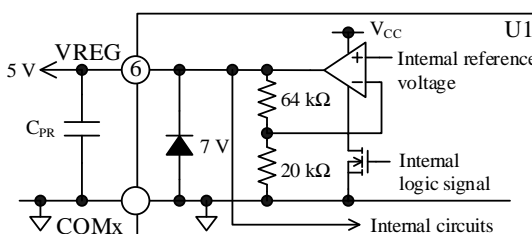


Figure 11-3. Internal Circuit Diagram of VREG Pin

This is the 5.0 V regulator output pin, which can be used for the power supply of the external Hall elements.

A maximum output current of the VREG pin is 30 mA. To stabilize the VREG pin output, connect a capacitor,  $C_{PR}$ , of about 0.1  $\mu\text{F}$  to the pin. The VREG pin also has the undervoltage lockout. For more details on this function, see Section 11.7.1.

## 11.1.6 CW/CCW

This is the setting pin which determines the direction of motor rotation. Table 11-2 lists the logic level definitions for the CW/CCW pin and the corresponding motor directions. And Figure 11-4 shows an internal circuit diagram of the CW/CCW pin. To set the CW/CCW pin to logic low, connect the pin to the GND pin. To set the CW/CCW pin to logic high, connect the pin to the VREG pin. The IC detects which logic level the CW/CCW pin has been set during a startup period (i.e., a period during which the VCC pin voltage is rising).

Table 11-2. Logic Levels Defined for CW/CCW Pin

CW/CCW Pin	Motor Direction
L	Forward (CW)
H	Reverse (CCW)

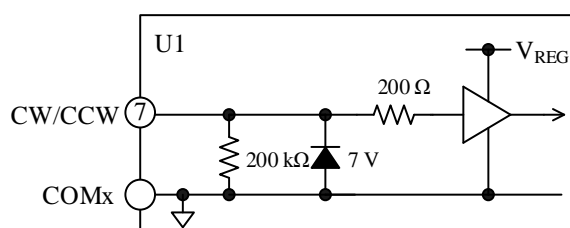


Figure 11-4. Internal Circuit Diagram of CW/CCW Pin

## 11.1.7 FGSEL

The FGSEL pin determines the cycle of a rotation pulse signal the FG pin outputs. Table 11-3 provides the relation between the FGSEL pin logic level and the number of pulses of a rotation pulse signal per 360° electrical angle. Figure 11-5 shows an internal circuit diagram of the FGSEL pin. To set the FGSEL pin to logic low, connect the pin to the GND pin. To set the FGSEL pin to logic high, connect the pin to the VREG pin. The IC detects which logic level the FGSEL pin has been set during a startup period (i.e., when the VCC pin voltage is rising).

Table 11-3. Number of Pulses of Rotation Pulse Signal

FGSEL Pin	Number of Signal Pulses
L	3 pulses per 360° electrical angle
H	1 pulse per 360° electrical angle

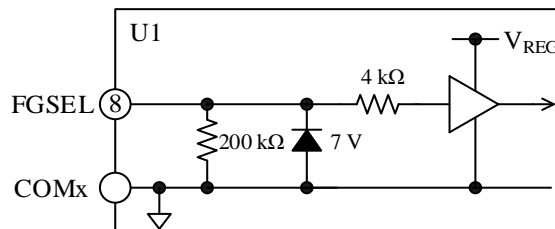


Figure 11-5. Internal Circuit Diagram of FGSEL Pin

## 11.1.8 HUP, HVP, and HWN; HUN, HVN, and HWP

These are the input pins for Hall element signals. The HxP pin is connected to the positive node of a Hall element, whereas the HxN pin is connected to the negative node of a Hall element. As Figure 11-6 illustrates, connect a noise filter capacitor,  $C_{Hx}$ , with a capacitance of about 0.1  $\mu\text{F}$ , between the HxP and HxN pins.  $C_{Hx}$  must be placed near the IC with a minimal length of traces. The IC incorporates the protection circuit that detects abnormal signals from the external Hall elements (see Section 11.7.7).

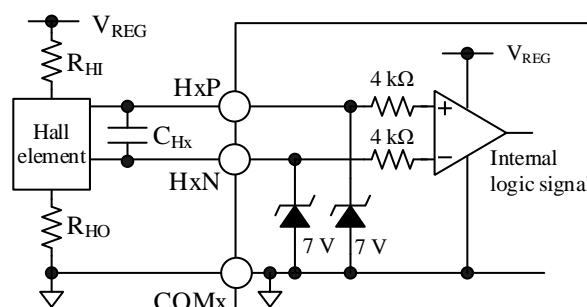


Figure 11-6. Internal Circuit Diagram of HxP and HxN Pins

## 11.1.9 VSP

The IC controls the speed of motor rotation with an analog voltage applied to the VSP pin. For more details on the motor speed control, see Section 11.4.

## 11.1.10 FG

The FG pin outputs a rotation pulse signal that is generated based on a position sensing signal. A rotation pulse signal is inverted at each edge of the Hall element signal assigned to the U-, V-, and W-phases. As shown in Figure 11-7, the FG pin is internally pulled down to the COMx pin.

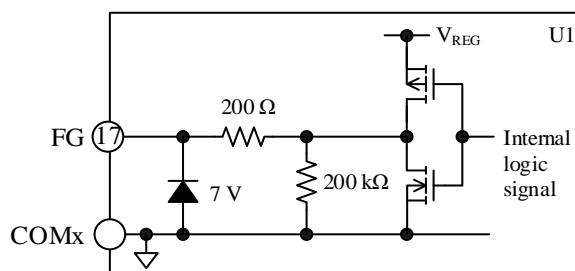


Figure 11-7. Internal Circuit Diagram of FG Pin

### 11.1.11 FO

The FO pin operates as the fault signal output. For more details on this function, see Section 11.6. Figure 11-8 shows an internal circuit diagram of the FO pin. The FO pin can also be directly connected to the input pin of the external microcontroller. For avoiding repeated OCP activations, the external microcontroller must shut off any input signals to the IC within an OCP hold time,  $t_P = 15$  ms, after a fault signal output. (For more details, see Section 11.7.3)

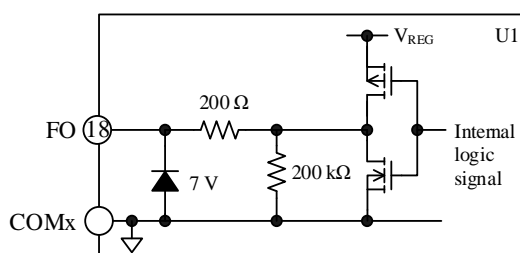


Figure 11-8. Internal Circuit Diagram of FO Pin

### 11.1.12 VCC

This is the logic supply pin for the built-in control ICs. The VCC pin has the undervoltage lockout for power supply (see Section 11.7.2.2). To prevent malfunction induced by supply ripples or other factors, put a 0.01  $\mu$ F to 0.1  $\mu$ F ceramic capacitor,  $C_P$ , near these pins. To prevent damage caused by surge voltages, put an 18 V to 20 V Zener diode, DZ, between the VCC and COMx pins. Voltages to be applied between the VCC and COMx pins should be regulated within the recommended operational range of  $V_{CC}$ , given in Section 2.

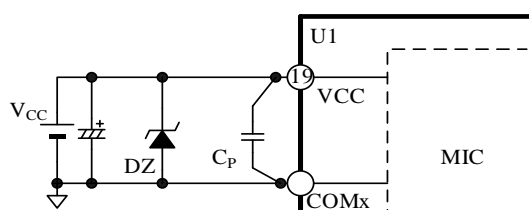


Figure 11-9. VCC Pin and Its Peripheral Circuit

### 11.1.13 VBB1 and VBB2

These are the input pins for the main supply voltage, i.e., the positive DC bus. All of the high-side drains (collectors) are connected to these pins. Voltages between the VBBx and COMx pins should be set within the recommended range of the main supply voltage,  $V_{DC}$ , given in Section 2.

To suppress surge voltages, put a 0.01  $\mu$ F to 0.1  $\mu$ F bypass capacitor,  $C_S$ , near the VBBx pin and an electrolytic capacitor,  $C_{DC}$ , with a minimal length of PCB traces to the VBBx pin.

### 11.1.14 VB1, VB2, and VB3

The VB1, VB2, and VB3 pins are connected to bootstrap capacitors,  $C_{Bx}$ , for the high-side floating supply. For proper startup, turn on the low-side transistors first, then fully charge the bootstrap capacitors,  $C_{Bx}$ . Section 11.2 describes the startup sequences of the IC in detail; Section 11.3 explains the procedures to charge the bootstrap capacitors.

$C_{Bx}$ , with a capacitance of about 1  $\mu$ F, must be placed near the IC, and connected between VBx and output (U, V1, W1) pins with a minimal length of traces. The VBx pin also has the undervoltage lockout for power supply. For more details on this function, see Section 11.7.2.1.

### 11.1.15 U, V1, V2, W1, and W2

These pins are the outputs of the three phases, and serve as the connection terminals to the 3-phase motor. The V1 and W1 pins must be connected to the V2 and W2 pins on a PCB, respectively. The U, V, and W1 pins are the grounds for the VB1, VB2, and VB3 pins. The U, V1, and W1 pins are connected to the negative nodes of bootstrap capacitors,  $C_{Bx}$ . Since high voltages are applied to these output pins (U, V1, V2, W1, W2), it is required to take measures for insulating as follows:

- Keep enough distance between the output pins and low-voltage traces.
- Coat the output pins with insulating resin.

### 11.1.16 LS1 and LS2

The LS1 pin is connected to the low-side source (emitter) of the U-phase; the LS2 pin is connected to the low-side sources (emitters) of the V- and W-phases. The LSx pin should be connected to an external shunt resistor,  $R_S$ , on a PCB. When connecting the shunt resistor, use the resistor with low inductance (required), and place it as near as possible to the IC with a minimum length of traces to the LSx and COMx pins. Otherwise, malfunction may occur because a longer circuit trace increases its inductance and thus increases its susceptibility to improper operations. In applications

where long PCB traces are required, add a fast recovery diode,  $D_{RS}$ , between the LSx and COMx pins in order to prevent the IC from malfunctioning.

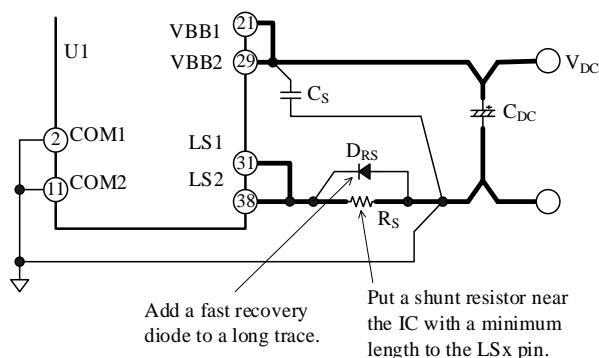


Figure 11-10. Connections to LSx Pin

## 11.2 Startup Operation

When the VCC pin voltage reaches  $V_{CC(ON)} = 11.5$  V, the IC starts operating. As the startup sequence starts, the IC detects and reflects the logic states of the following pins to the motor control settings: the MLP, CW/CCW, and FGSEL pins. The IC then waits for the VSP pin voltage to reach a certain level at which output duty cycles are controllable. At startup, the IC operates according to the VSP pin voltage levels as follows:

- **$V_{SP} < 1.0$  V:**  
All the output signals are off.
- **$1.0$  V  $\leq V_{SP} < 2.1$  V:**  
The IC starts charging bootstrap capacitors. For more details, see Section 11.3.
- **$2.1$  V  $\leq V_{SP} \leq 5.4$  V:**  
The IC controls its output duty cycles according to the VSP pin voltage levels. While the frequency of a position sensing signal, Hx, is less than 1.0 Hz at startup, the motor is driven by a trapezoidal control. When Hx increases to 1.0 Hz or more (i.e., the condition in which a position sensing signal is detected at every rotation of 60° in electrical degrees), the IC generates a sine-wave signal and drives the motor by a sinusoidal control.

Table 11-4 and Table 11-5 are truth tables for the motor driven by the trapezoidal control in a forward or reverse rotation. Moreover, the timing charts shown later represent the operational waveforms in the following motor operations: the motor in a forward rotation (no phase advance; Figure 11-15), the motor in a forward rotation (phase advance by 15°; Figure 11-16), and the motor in a reverse rotation (Figure 11-17). The following symbols used in Figure 11-15 to Figure 11-17 represent the signals generated inside the IC:  $S_U$ ,  $S_V$ ,  $S_W$ ,  $S_X$ ,  $S_Y$ ,  $S_Z$ . Then the IC detects a state in which the motor rotates inversely to the preset direction, the motor driving system is immediately switched to the

trapezoidal control before a rotation of 60° electrical angle completes. For detailed descriptions on the reverse rotation detection, see Section 11.7.6.

The following are the important considerations for appropriate power startup and shutdown sequences.

- To turn on the IC, be sure to increase the VSP pin voltage last. To turn off the IC, be sure to decrease the VSP pin voltage first.
- When you have enabled the motor lock protection (MLP = L), be sure to apply a voltage to the VBBx pin at the timing described below. At startup, apply a voltage to the VCC pin and the VREG pin voltage,  $V_{REG}$ , increases. Then, apply a main supply voltage to the VBBx pin within the period from  $V_{REG}$  increase to an MLP detection time,  $t_{LD}$ . When a position sensing signal stays unchanged even after a lapse of  $t_{LD}$ , the IC determines this condition as a motor lockup state and activates the motor lock protection (see Section 11.7.5).

The IC can also operate in test mode. In test mode, the high-side transistors in the trapezoidal control are driven at duty cycle = 100%, the TSD circuit is disabled, and the phase advance angle is fixed at 0°. To start IC operations in test mode, turn on the IC after applying a voltage of  $\geq 8.1$  V on the VSP pin, and a voltage of 2.75 V (typ.) on the CW/CCW pin.

## 11.3 Charging of Bootstrap Capacitors

It is required to fully charge bootstrap capacitors,  $C_{Bx}$ , at startup. The charging sequence depends on the VSP pin voltage,  $V_{SP}$ . When  $1.0$  V  $\leq V_{SP} \leq 2.1$  V at startup, the IC turns on the low-side transistors at every PWM cycle in order to charge  $C_{Bx}$ . When  $V_{SP} \geq 2.1$  V, the IC controls the motor speed according to the VSP pin voltage levels (see Section 11.4). However, note that the IC does not charge  $C_{Bx}$  even when  $1.0$  V  $\leq V_{SP} \leq 2.1$  V along with the motor rotating inversely to the preset direction, or the motor coasting at a frequency of  $\geq 1.0$  Hz. If a sudden rise in the VSP pin voltage up to 2.1 V or more occurs at startup, the IC starts the motor speed control after charging  $C_{Bx}$  for a period of 9 ms  $\pm$  5%.

## 11.4 Motor Speed Control

The IC controls the speed of motor rotation with an analog voltage applied to the VSP pin. When  $2.1\text{ V} \leq V_{SP} \leq 5.4\text{ V}$ , the IC controls its output duty cycles depending on the VSP pin voltage levels. For the IC operation when  $V_{SP} < 2.1\text{ V}$  (i.e., the startup sequence), see Section 11.2.

A duty cycle of an output signal is determined according to a digital signal that is generated by the built-in 7-bit AD converter from the VSP pin input voltage. The higher the VSP pin voltage increases, the higher the duty cycle becomes, thus causing the motor to rotate faster. Figure 11-11 depicts how a duty cycle varies according to the VSP pin voltage,  $V_{SP}$ . While  $V_{SP}$  maintains at 5.4 V or more, the IC controls its output signals at duty cycle = 100%.

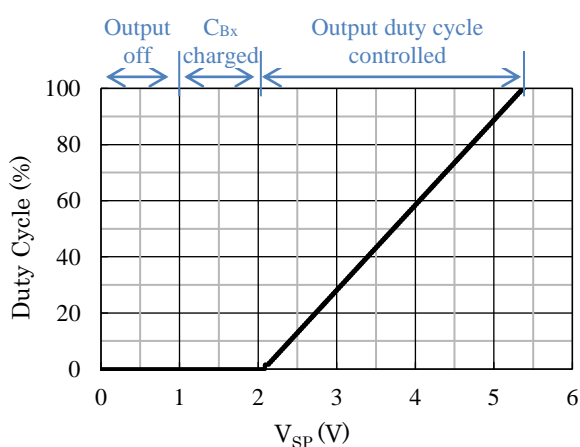


Figure 11-11. VSP Pin Voltage vs. Duty Cycle

Figure 11-12 is an internal circuit diagram describing the VSP pin and its peripheral circuit. A voltage to be applied on the VSP pin,  $V_{SPP}$ , must be set to  $<10\text{ V}$ , i.e., below the rated VSP pin input voltage.  $R_{SP}$  should have a resistance of about  $100\ \Omega$ ;  $C_{SP}$  should have a capacitance of about  $0.1\ \mu\text{F}$ .

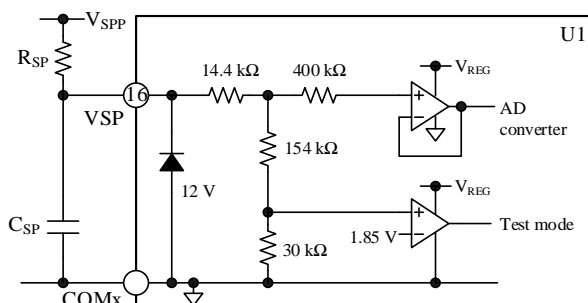


Figure 11-12. Internal Circuit Diagram of VSP Pin and Its Peripheral Circuit

## 11.5 Phase Advance Function

The IC features the phase advance function. The angle of phase advance is determined by an analog voltage applied to the LA pin. As shown in Figure 11-13, the VREG pin voltage divided by two resistors,  $R_{LA1}$  and  $R_{LA2}$ , is applied to the LA pin. Figure 11-14 plots how a phase advance angle changes over the LA pin voltage. When the phase advance function is enabled, each phase shifts  $\pm 0.9375^\circ$  every 4 cycles of a Hall signal to the preset angle.

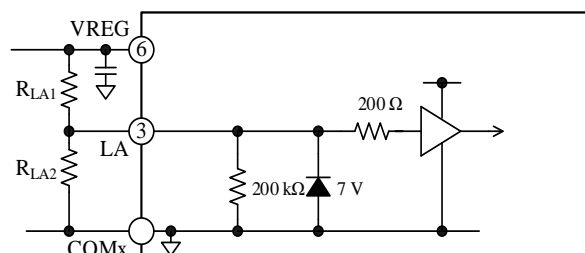


Figure 11-13. Internal Circuit Diagram of LA Pin

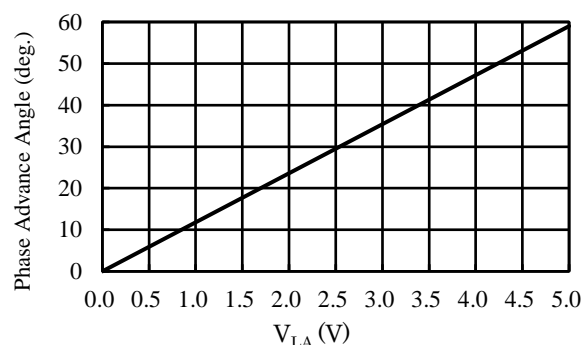


Figure 11-14. LA Pin Voltage vs. Phase Advance Angle

Table 11-4. Truth Table for Trapezoidal Control (Forward)

Position Sensing Signal			U-phase		V-phase		W-phase	
HU	HV	HW	High-side Transistor	Low-side Transistor	High-side Transistor	Low-side Transistor	High-side Transistor	Low-side Transistor
H	L	H	OFF	ON	ON	OFF	OFF	OFF
H	L	L	OFF	ON	OFF	OFF	ON	OFF
H	H	L	OFF	OFF	OFF	ON	ON	OFF
L	H	L	ON	OFF	OFF	ON	OFF	OFF
L	H	H	ON	OFF	OFF	OFF	OFF	ON
L	L	H	OFF	OFF	ON	OFF	OFF	ON
L	L	L	OFF	OFF	OFF	OFF	OFF	OFF
H	H	H	OFF	OFF	OFF	OFF	OFF	OFF

Table 11-5. Truth Table for Trapezoidal Control (Reverse)

Position Sensing Signal			U-phase		V-phase		W-phase	
HU	HV	HW	High-side Transistor	Low-side Transistor	High-side Transistor	Low-side Transistor	High-side Transistor	Low-side Transistor
L	H	L	OFF	ON	ON	OFF	OFF	OFF
L	H	H	OFF	ON	OFF	OFF	ON	OFF
L	L	H	OFF	OFF	OFF	ON	ON	OFF
H	L	H	ON	OFF	OFF	ON	OFF	OFF
H	L	L	ON	OFF	OFF	OFF	OFF	ON
H	H	L	OFF	OFF	ON	OFF	OFF	ON
H	H	H	OFF	OFF	OFF	OFF	OFF	OFF
L	L	L	OFF	OFF	OFF	OFF	OFF	OFF



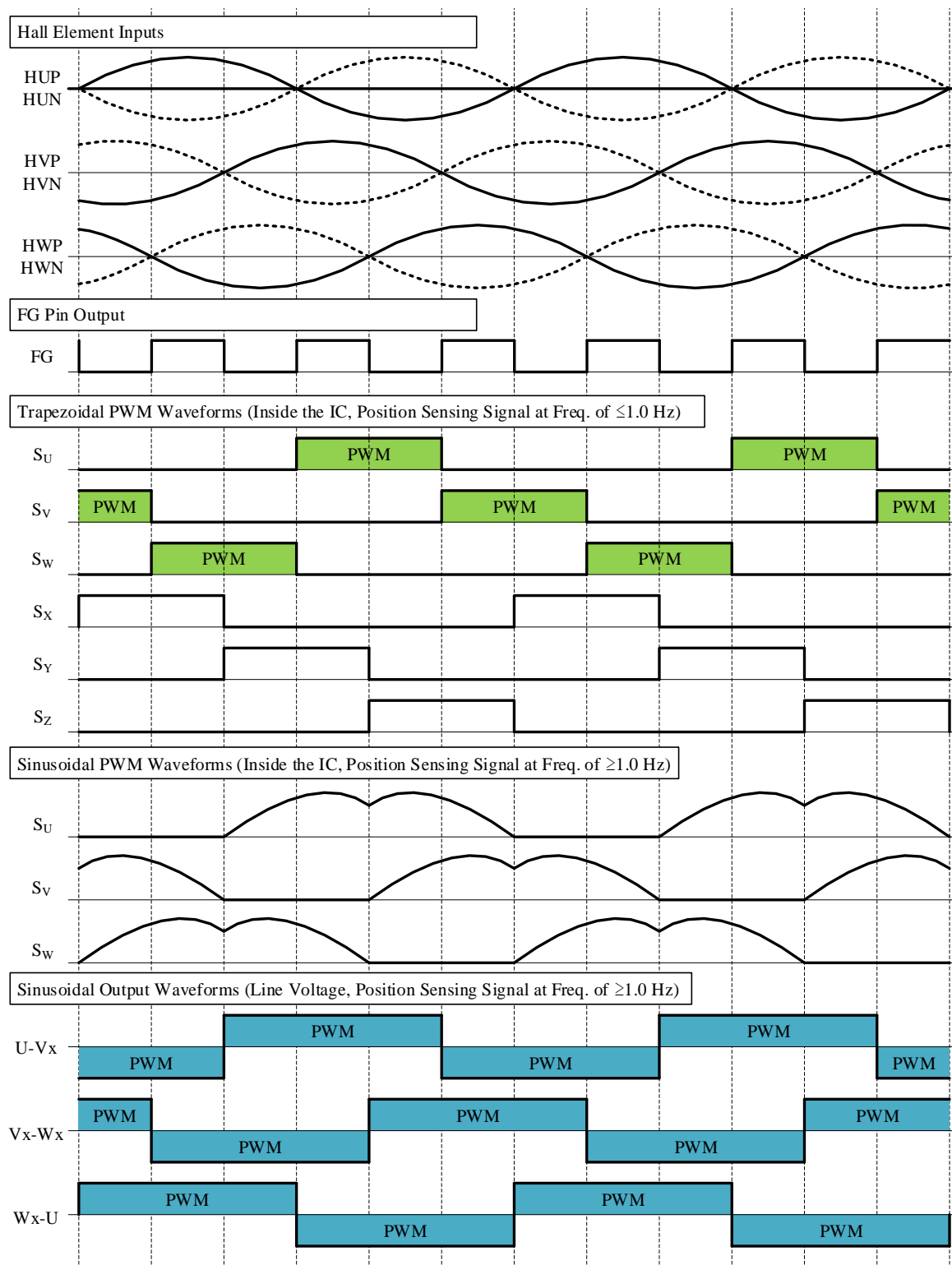
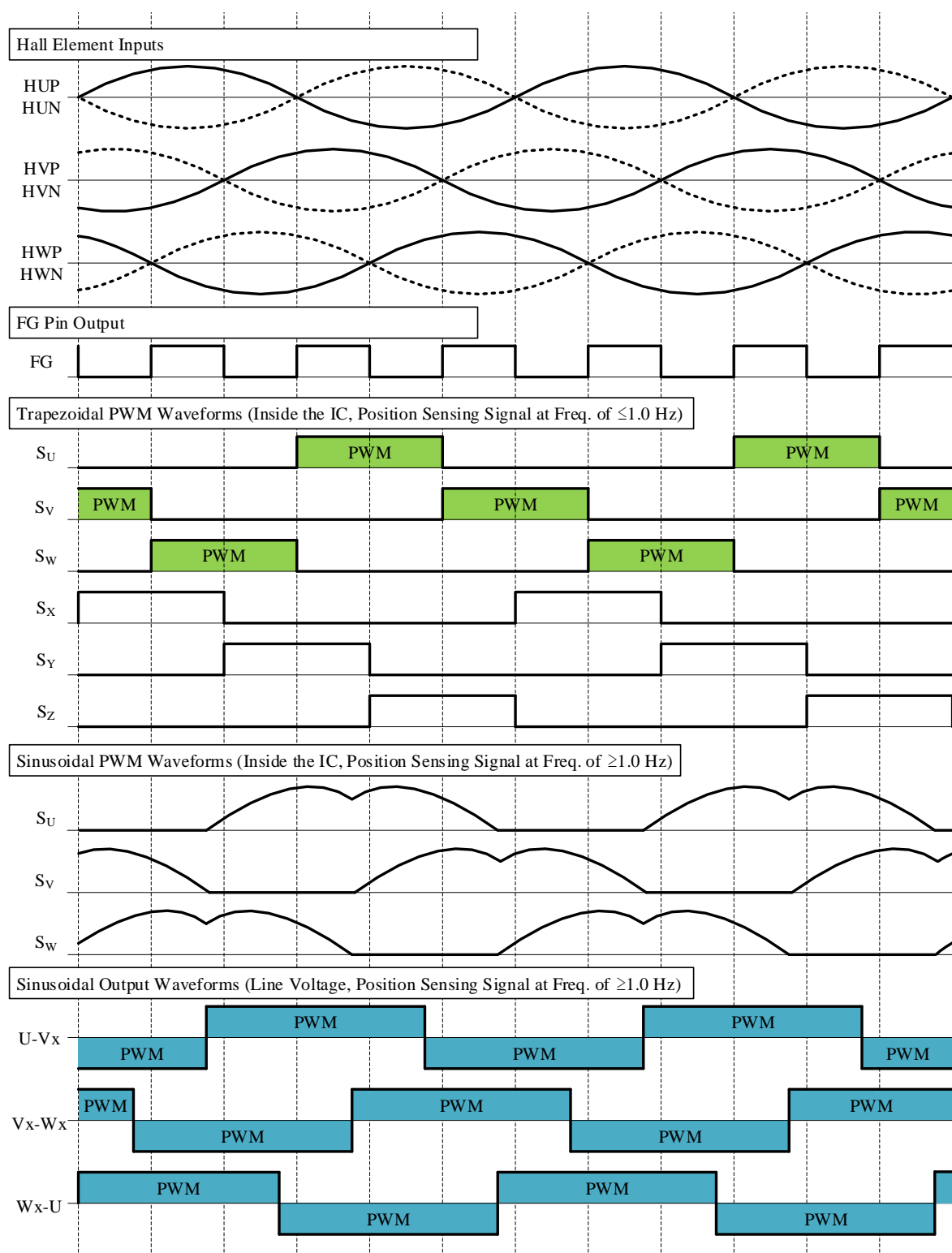


Figure 11-15. Operational Waveforms (Forward, No Phase Advance)



Figure 11-16. Operational Waveforms (Forward, Phase Advance by  $15^\circ$ )

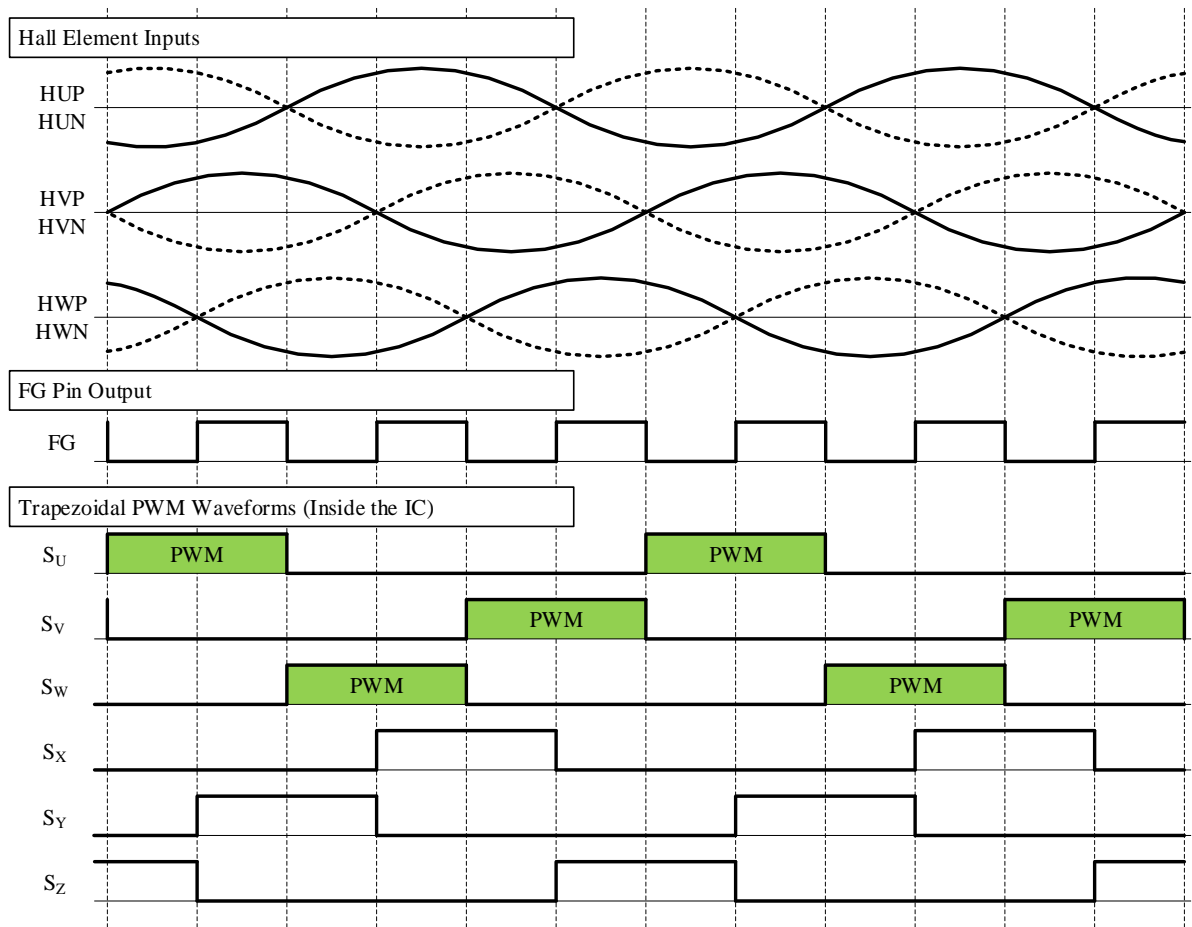


Figure 11-17. Operational Waveforms (Reverse)

## 11.6 Fault Signal Output

In case one or more of the following protections are actuated, an internal P-channel power MOSFET turns on, then the FO pin becomes logic high (about 5 V). In normal operation, the FO pin outputs a low signal.

For more details on the protections, see Section 11.7.

- VREG pin undervoltage lockout (UVLO\_VREG)
- Overcurrent protection (OCP)
- Thermal shutdown (TSD)
- Motor lock protection (MLP)
- Reverse rotation detection
- Hall signal abnormality detection

The fault signal output time of the FO pin at OCP activation is defined as the OCP Hold Time,  $t_p = 15$  ms (typ.), fixed by a built-in feature of the IC itself (see Section 11.7.3).

The external microcontroller receives a fault signal with its interrupt pin (INT), and must be programmed to shut off any input signals to the IC within the predetermined OCP hold time,  $t_p$ .

## 11.7 Protection Functions

This section describes the various protection circuits provided in the SIM260xM series, such as those designed to detect a voltage drop across power supplies, an overcurrent condition, an abnormal motor state, and so on.

### 11.7.1 VREG Pin Undervoltage Lockout (UVLO VREG)

When the VREG pin voltage decreases to  $V_{UVRL} = 3.60\text{ V}$  or less, the VREG pin undervoltage lockout (UVLO\_VREG) circuit gets activated and turns off the high- and low-side transistors. When the VREG pin voltage increases to  $V_{UVRH} = 4.00\text{ V}$  or more, the IC releases the UVLO\_VREG operation. Then, the high- and low-side transistors resume operating according to position sensing signals. During the UVLO\_VREG operation, the FO pin becomes logic high and transmits fault signals.

### 11.7.2 Undervoltage Lockout for Power Supply (UVLO)

In case the gate-driving voltages of the output transistors decrease, their steady-state power dissipations increase. This overheating condition may cause permanent damage to the IC in the worst case. To prevent this event, the SIM260xM series has the undervoltage lockout (UVLO) circuits for each of the high-side (the VBx pin) and the low-side (the VCC pin) power supplies.

### 11.7.2.1. VBx Pin (UVLO\_VB)

When the voltage between the VBx and output (U, V1/V2, or W1/W2) pins (VBx–HSx) decreases to  $V_{BS(OFF)} = 10.0\text{ V}$  or less, the UVLO\_VB circuit gets activated and turns off the high-side transistors. When the voltage between the VBx and output pins increases to  $V_{BS(ON)} = 10.5\text{ V}$  or more, the IC releases the UVLO\_VB operation. Then, the high-side transistors resume operating according to position sensing signals.

#### 11.7.2.2. VCC Pin (UVLO\_VCC)

When the VCC pin voltage decreases to  $V_{CC(OFF)} = 11.0\text{ V}$  or less, the UVLO\_VCC circuit gets activated and turns off the high- and low-side transistors. When the VCC pin voltage increases to  $V_{CC(ON)} = 11.5\text{ V}$  or more, the IC releases the UVLO\_VCC operation. Then, the high- and low-side transistors resume operating according to position sensing signals.

### 11.7.3 Overcurrent Limit (OCL) and Overcurrent Protection (OCP)

The IC has two different protections against overcurrent conditions: the overcurrent limit (OCL) and the overcurrent protection (OCP). Figure 11-18 is an internal circuit diagram describing the OCP pin and its peripheral circuit. The OCP pin detects overcurrents with voltage across an external shunt resistor,  $R_s$ . Because the OCP pin is internally pulled up, the OCP pin voltage increases proportionally to a rise in the current running through the shunt resistor,  $R_s$ . When the shunt resistor,  $R_s$ , is open, the IC activates the OCP function.

Note that overcurrents are undetectable when one or more of the U, V1/V2, and W1/W2 pins or their traces are shorted to ground (ground fault). In case any of these pins falls into a state of ground fault, the output transistors may be destroyed.

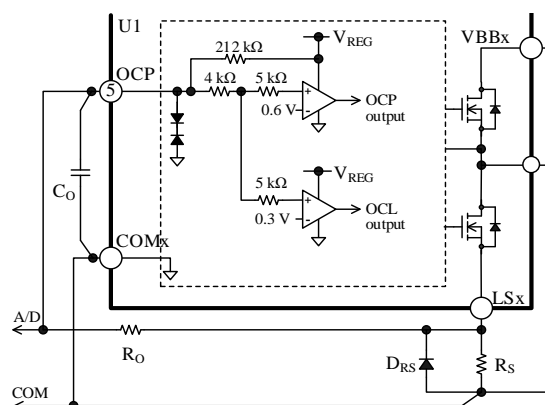


Figure 11-18. Internal Circuit Diagram of OCP Pin and Its Peripheral Circuit

The overcurrent limit (OCL) is a protection against relatively low overcurrent conditions. When the OCP pin voltage increases to  $V_{LIM} = 0.30$  V or more, and remains in this condition for a period of a blanking time ( $t_{BK(OCL)} = 2.3$   $\mu$ s) or longer, the IC turns off the high- and low-side transistors. The OCL operation is automatically released at each PWM cycle.

The overcurrent protection (OCP) is a protection against large inrush currents. When the OCP pin voltage increases to  $V_{TRIP} = 0.60$  V or more, and remains in this condition for a period of a blanking time ( $t_{BK(OCP)} = 0.8$   $\mu$ s) or longer, the OCP circuit is activated. Then, the high- and low-side transistors are turned off for a certain period of time ( $t_P = 15$  ms). After that, the high- and low-side transistors resume operating according to position sensing signals. During the OCP operation, the FO pin goes logic high and sends fault signals.

The OCL and OCP are used for detecting abnormal conditions, such as an output transistor shorted. In case short-circuit conditions occur repeatedly, the output transistors can be destroyed. For this reason, motor operations must be controlled by the external microcontroller so that it can immediately stop the motor when fault signals are detected. If you need to resume the IC operation thereafter, set the IC to be resumed after a lapse of  $\geq 2$  seconds.

For proper shunt resistor setting, your application must meet the following:

- Use the shunt resistor that has a recommended resistance,  $R_S$  (see Section 2).
- Set the OCP pin input voltage to vary within the rated input voltages,  $V_{IN(2)}$  (see Section 1).
- Keep the current through the output transistors below the rated output current (pulse),  $I_{OP}$  (see Section 1).

It is required to use a resistor with low internal inductance because high-frequency switching current will flow through the shunt resistor,  $R_S$ . In addition, choose a resistor with allowable power dissipation according to your application.

### 11.7.4 Thermal Shutdown (TSD)

The SIM260xM series incorporates the thermal shutdown (TSD) circuit. In case of overheating (e.g., increased power dissipation due to overload, or elevated ambient temperature at the device), the IC shuts down the high- and low-side transistors.

The TSD circuit in the MIC for gate driver monitors temperatures (see Figure 6-1). When the junction temperature of the MIC for gate driver,  $T_{J(DRV)}$ , exceeds  $T_{DH} = 130$  °C, the TSD circuit is activated. When  $T_{J(DRV)}$  decreases to  $T_{DH} - T_{D(HYS)}$  after the TSD activation, the shutdown condition is released. The output transistors then resume operating according to input signals. During the TSD operation, the FO pin becomes logic high and

transmits fault signals. Note that junction temperatures of the output transistors themselves are not monitored; therefore, do not use the TSD function as an overtemperature prevention for the output transistors.

### 11.7.5 Motor Lock Protection (MLP)

When the state in which a position sensing signal stays unchanged within a rotation of 60° electrical angle persists for a motor lock hold time ( $t_{LD} = 5$  s) or longer, the motor lock protection (MLP) circuit gets activated. Then, the high- and low-side transistors are turned off for a certain period of time ( $t_{LH} = 64$  s). After that, the high- and low-side transistors resume operating according to position sensing signals.

During the MLP operation, the FO pin becomes logic high and transmits fault signals. Moreover, direct currents through the output transistors cause an increase in the junction temperatures of the output transistors. Therefore, care must be taken not to allow the junction temperatures to exceed the absolute maximum rating.

### 11.7.6 Reverse Rotation Detection

In case the motor rotates in a direction opposite to the preset direction, the reverse rotation detection function gets activated and puts the FO pin into a high state (i.e., a fault signal output). When the motor rotates in the preset direction, the FO pin is in a low state. When the IC detects a reverse rotation state during motor rotations, the motor driving system is immediately switched to the trapezoidal control before a rotation of 60° electrical angle completes.

Table 11-6. Motor Driving Controls during Reverse Rotation

CW/CCW Pin State	Motor Direction	Driving System
L (Forward)	Forward	Sinusoidal
	Reverse	Trapezoidal
H (Reverse)	Forward	Trapezoidal
	Reverse	Sinusoidal

### 11.7.7 Hall Signal Abnormality Detection

As Figure 11-19 shows, signals from the external Hall elements are input into the corresponding comparators. The IC then receives the comparator outputs as the motor positional information, i.e., position sensing signals.

When all the position sensing signals (HU, HV, HW) are either in a high or low state, the Hall signal abnormality detection function gets activated and turns off the high- and low-side transistors. When the IC

detects input states other than those above, each of the high- and low-side transistors responds in accordance with the input logic levels of the position sensing signals. For the truth tables for the position sensing signals and the output transistors, see Table 11-4 and Table 11-5. While the function is being enabled, the FO pin becomes logic high and sends fault signals.

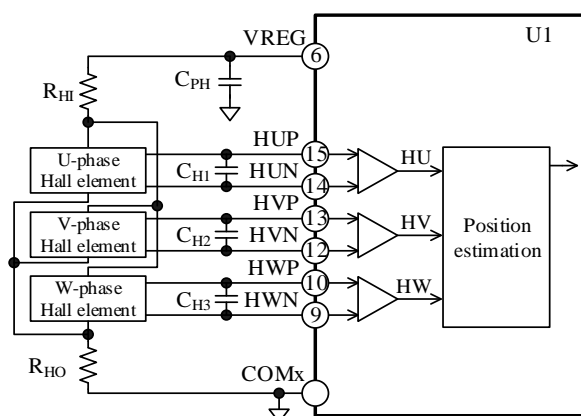


Figure 11-19. Internal Circuit Diagram of HxP and HxN Pins and Their Peripheral Circuit

## 12. Design Notes

### 12.1 PCB Pattern Layout

Figure 12-1 shows a schematic diagram of a motor drive circuit. The circuit consists of current paths having high frequencies and high voltages, which also bring about negative influences on IC operation, noise interference, and power dissipation. Therefore, PCB trace layouts and component placements play an important role in circuit designing. Current loops, which have high frequencies and high voltages, should be as small and wide as possible, in order to maintain a low-impedance state. In addition, ground traces should be as wide and short as possible so that radiated EMI levels can be reduced.

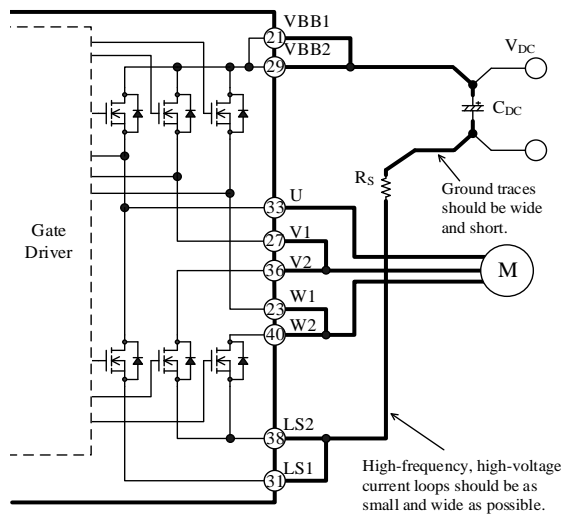


Figure 12-1. High-frequency, High-voltage Current Paths

### 12.2 Considerations in IC Characteristics Measurement

When measuring the leakage current of the output transistors incorporated in the IC, note that all of the output (U, V1, V2, W1, W2), LSx, and COMx pins must be appropriately connected. Otherwise, the output transistors may result in permanent damage. Also note that the gate and source (emitter) of each output transistor should have the same potential during the leakage current measurement. Moreover, care should be taken during the measurement because each output transistor is connected as follows:

- All the high-side drains (collectors) are internally connected to the VBBx pin.
- In the U-phase, the high-side source (emitter) and the low-side drain (collector) are internally connected to the U pin. (In the V- and W-phases, the high- and low-side transistors are unconnected inside the IC.)

- In the V- and W-phases, the low-side sources (emitters) are internally connected to the LS2 pin.
- The high-side gates are internally pulled down to the output pins.
- The low-side gates are internally pulled down to the COMx pin.

The following are circuit diagrams representing typical measurement circuits for breakdown voltage: Figure 12-2 shows the high-side transistor ( $Q_{1H}$ ) in the U-phase; Figure 12-3 shows the low-side transistor ( $Q_{1L}$ ) in the U-phase. And all the pins that are not represented in these figures are open. When measuring the high-side transistors, leave all the non-measuring pins open. When measuring the low-side transistors, connect only the measuring LSx pin to the COMx pin and leave the other pins open.

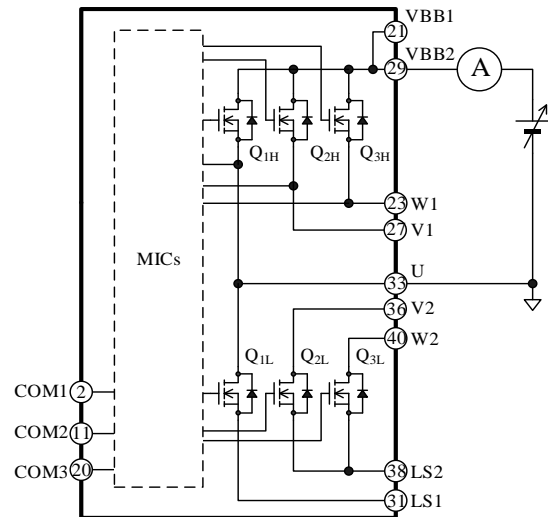


Figure 12-2. Typical Measurement Circuit for High-side Transistor ( $Q_{1H}$ ) in U-phase

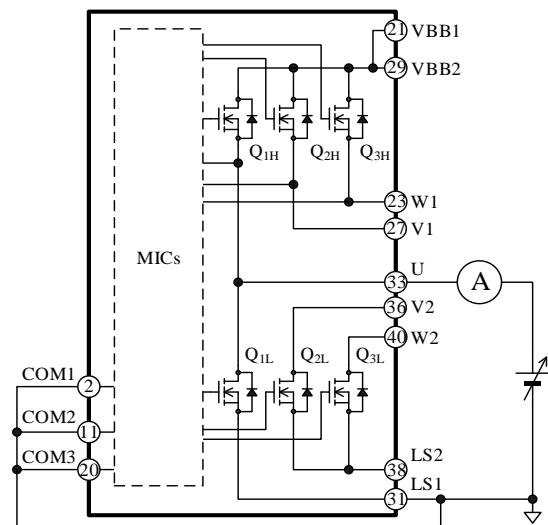


Figure 12-3. Typical Measurement Circuit for Low-side Transistor ( $Q_{1L}$ ) in U-phase

### 12.3 Considerations in Heatsink Mounting

The following are the key considerations and the guidelines for mounting a heatsink:

- A pair of a metric screw of M2.5 and a plain washer of 6.0 mm ( $\phi$ ) must be used. When tightening the screws, use a torque screwdriver and tighten them within the range of screw torque defined in Section 4. Be sure to avoid uneven tightening. Temporarily tighten the two screws first, then tighten them equally on both sides until the specified screw torque is reached.
- When mounting a heatsink, it is recommended to use silicone greases. If a thermally conductive sheet or an electrically insulating sheet is used, package cracks may be occurred due to creases at screw tightening. Therefore, you should conduct thorough evaluations before using these materials.
- When applying a silicone grease, make sure that there are no foreign substances between the IC and a heatsink. Extreme care should be taken not to apply a silicone grease onto any device pins as much as possible. The following requirements must be met for proper grease application:
  - Grease thickness: 100  $\mu\text{m}$
  - Heatsink flatness:  $\pm 100 \mu\text{m}$
  - Apply a silicone grease within the area indicated in Figure 12-4, below.

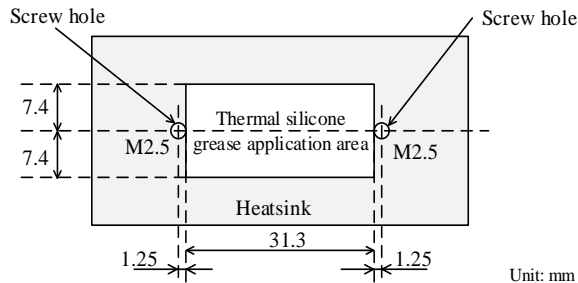


Figure 12-4. Reference Application Area for Thermal Silicone Grease

## 13. Calculating Power Losses and Estimating Junction Temperature

This section describes the procedures to calculate power losses in switching transistors, and to estimate a junction temperature. Note that the descriptions listed here are applicable to the SIM260xM series, which is controlled by a 3-phase sine-wave PWM driving strategy. For quick and easy references, we offer calculation support tools online. Please visit our website to find out more.

- DT0050: SIM2601MA Calculation Tool  
[https://www.semicon.sanken-ele.co.jp/en/calc-tool/igbtall\\_caltool\\_en.html](https://www.semicon.sanken-ele.co.jp/en/calc-tool/igbtall_caltool_en.html)

[tool/mosfet\\_caltool\\_en.html](https://www.semicon.sanken-ele.co.jp/en/calc-tool/mosfet_caltool_en.html)

- DT0052: SIM2602M Calculation Tool  
[https://www.semicon.sanken-ele.co.jp/en/calc-tool/igbtall\\_caltool\\_en.html](https://www.semicon.sanken-ele.co.jp/en/calc-tool/igbtall_caltool_en.html)

### 13.1 Power MOSFET

Total power loss in a power MOSFET can be obtained by taking the sum of the following losses: steady-state loss,  $P_{\text{RON}}$ ; switching loss,  $P_{\text{SW}}$ ; the steady-state loss of a body diode,  $P_{\text{SD}}$ . In the calculation procedure we offer, the recovery loss of a body diode,  $P_{\text{RR}}$ , is considered negligibly small compared with the ratios of other losses.

The following subsections contain the mathematical procedures to calculate these losses ( $P_{\text{RON}}$ ,  $P_{\text{SW}}$ , and  $P_{\text{SD}}$ ) and the junction temperature of all power MOSFETs operating.

#### 13.1.1 Power MOSFET Steady-state Loss, $P_{\text{RON}}$

Steady-state loss in a power MOSFET can be computed by using the  $R_{\text{DS(ON)}}$  vs.  $I_{\text{D}}$  curves, listed in Section 14.3.1. As expressed by the curves in Figure 13-1, a linear approximation at a range the  $I_{\text{D}}$  is actually used is obtained by:  $R_{\text{DS(ON)}} = \alpha \times I_{\text{D}} + \beta$ . The values gained by the above calculation are then applied as parameters in Equation (1), below. Hence, the equation to obtain the power MOSFET steady-state loss,  $P_{\text{RON}}$ , is:

$$\begin{aligned}
 P_{\text{RON}} &= \frac{1}{2\pi} \int_0^\pi I_{\text{D}}(\varphi)^2 \times R_{\text{DS(ON)}}(\varphi) \times DT \times d\varphi \\
 &= 2\sqrt{2}\alpha \left( \frac{1}{3\pi} + \frac{3}{32} M \times \cos\theta \right) I_{\text{M}}^3 \\
 &\quad + 2\beta \left( \frac{1}{8} + \frac{1}{3\pi} M \times \cos\theta \right) I_{\text{M}}^2. \quad (1)
 \end{aligned}$$

Where:

$I_{\text{D}}$  is the drain current of the power MOSFET (A),  
 $R_{\text{DS(ON)}}$  is the drain-to-source on-resistance of the power MOSFET ( $\Omega$ ),  
 $DT$  is the duty cycle, which is given by

$$DT = \frac{1 + M \times \sin(\varphi + \theta)}{2},$$

$M$  is the modulation index (0 to 1),  
 $\cos\theta$  is the motor power factor (0 to 1),  
 $I_{\text{M}}$  is the effective motor current (A),  
 $\alpha$  is the slope of the linear approximation in the  $R_{\text{DS(ON)}}$  vs.  $I_{\text{D}}$  curve, and  
 $\beta$  is the intercept of the linear approximation in the  $R_{\text{DS(ON)}}$  vs.  $I_{\text{D}}$  curve.



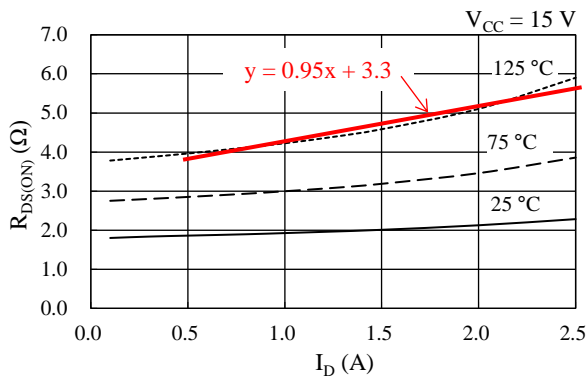


Figure 13-1. Linear Approximate Equation of  $R_{DS(ON)}$  vs.  $I_D$

### 13.1.2 Power MOSFET Switching Loss, $P_{SW}$

Switching loss in a power MOSFET can be calculated by Equation (2), letting  $I_M$  be the effective current value of the motor:

$$P_{SW} = \frac{\sqrt{2}}{\pi} \times f_C \times \alpha_E \times I_M \times \frac{V_{DC}}{300}. \quad (2)$$

Where:

$f_C$  is the PWM carrier frequency (Hz),  
 $V_{DC}$  is the main power supply voltage (V), i.e., the VBBx pin input voltage, and  
 $\alpha_E$  is the slope on the switching loss curve (see Section 14.3.2).

### 13.1.3 Body Diode Steady-state Loss, $P_{SD}$

Steady-state loss in the body diode of a power MOSFET can be computed by using the  $V_{SD}$  vs.  $I_{SD}$  curves, listed in Section 14.3.1. As expressed by the curves in Figure 13-2, a linear approximation at a range the  $I_{SD}$  is actually used is obtained by:  $V_{SD} = \alpha \times I_{SD} + \beta$ . The values gained by the above calculation are then applied as parameters in Equation (3), below. Hence, the equation to obtain the body diode steady-state loss,  $P_{SD}$ , is:

$$P_{SD} = \frac{1}{2\pi} \int_0^\pi V_{SD}(\varphi) \times I_{SD}(\varphi) \times (1 - DT) \times d\varphi$$

$$= \frac{1}{2} \alpha \left( \frac{1}{2} - \frac{4}{3\pi} M \times \cos \theta \right) I_M^2 + \frac{\sqrt{2}}{\pi} \beta \left( \frac{1}{2} - \frac{\pi}{8} M \times \cos \theta \right) I_M. \quad (3)$$

Where:

$V_{SD}$  is the source-to-drain diode forward voltage of the power MOSFET (V),

$I_{SD}$  is the source-to-drain diode forward current of the power MOSFET (A),

DT is the duty cycle, which is given by

$$DT = \frac{1 + M \times \sin(\varphi + \theta)}{2},$$

M is the modulation index (0 to 1),

$\cos \theta$  is the motor power factor (0 to 1),

$I_M$  is the effective motor current (A),

$\alpha$  is the slope of the linear approximation in the  $V_{SD}$  vs.  $I_{SD}$  curve, and

$\beta$  is the intercept of the linear approximation in the  $V_{SD}$  vs.  $I_{SD}$  curve.

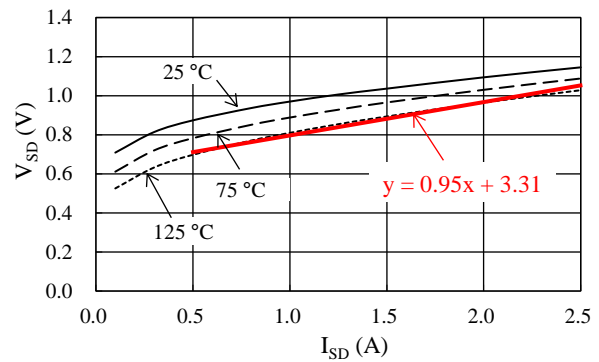


Figure 13-2. Linear Approximate Equation of  $V_{SD}$  vs.  $I_{SD}$  Curve

### 13.1.4 Estimating Junction Temperature of Power MOSFET

The junction temperature of all power MOSFETs operating,  $T_J$ , can be estimated with Equation (4):

$$T_J = R_{J-C} \times \{(P_{ON} + P_{SW} + P_{SD}) \times 6\} + T_C. \quad (4)$$

Where:

$R_{J-C}$  is the junction-to-case thermal resistance ( $^{\circ}\text{C}/\text{W}$ ) of all the power MOSFETs operating, and

$T_C$  is the case temperature ( $^{\circ}\text{C}$ ), measured at the point defined in Figure 3-2.



## 13.2 IGBT

Total power loss in an IGBT can be obtained by taking the sum of steady-state loss,  $P_{ON}$ , and switching loss,  $P_{SW}$ . The following subsections contain the mathematical procedures to calculate these losses ( $P_{ON}$  and  $P_{SW}$ ) and the junction temperature of all IGBTs operating.

### 13.2.1 IGBT Steady-state Loss, $P_{ON}$

Steady-state loss in an IGBT can be computed by using the  $V_{CE(SAT)}$  vs.  $I_C$  curves, listed in Section 14.3.1. As expressed by the curves in Figure 13-3, linear approximations at a range the  $I_C$  is actually used are obtained by:  $V_{CE(SAT)} = \alpha \times I_C + \beta$ . The values gained by the above calculation are then applied as parameters in Equation (5), below. Hence, the equation to obtain the IGBT steady-state loss,  $P_{ON}$ , is:

$$P_{ON} = \frac{1}{2\pi} \int_0^\pi V_{CE(SAT)}(\varphi) \times I_C(\varphi) \times DT \times d\varphi$$

$$= \frac{1}{2} \alpha \left( \frac{1}{2} + \frac{4}{3\pi} M \times \cos \theta \right) I_M^2 + \frac{\sqrt{2}}{\pi} \beta \left( \frac{1}{2} + \frac{\pi}{8} M \times \cos \theta \right) I_M \quad (5)$$

Where:

$V_{CE(SAT)}$  is the collector-to-emitter saturation voltage of the IGBT (V),

$I_C$  is the collector current of the IGBT (A),

$DT$  is the duty cycle, which is given by

$$DT = \frac{1 + M \times \sin(\varphi + \theta)}{2},$$

$M$  is the modulation index (0 to 1),

$\cos \theta$  is the motor power factor (0 to 1),

$I_M$  is the effective motor current (A),

$\alpha$  is the slope of the linear approximation in the  $V_{CE(SAT)}$  vs.  $I_C$  curve, and

$\beta$  is the intercept of the linear approximation in the  $V_{CE(SAT)}$  vs.  $I_C$  curve.

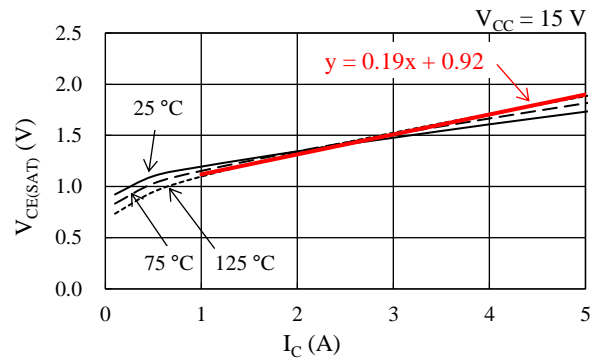


Figure 13-3. Linear Approximate Equation of  $V_{CE(SAT)}$  vs.  $I_C$

### 13.2.2 IGBT Switching Loss, $P_{SW}$

Switching loss in an IGBT,  $P_{SW}$ , can be calculated by Equation (6), letting  $I_M$  be the effective current value of the motor:

$$P_{SW} = \frac{\sqrt{2}}{\pi} \times f_c \times \alpha_E \times I_M \times \frac{V_{DC}}{300} \quad (6)$$

Where:

$f_c$  is the PWM carrier frequency (Hz),

$V_{DC}$  is the main power supply voltage (V), i.e., the VBBx pin input voltage, and

$\alpha_E$  is the slope on the switching loss curve (see Section 14.3.2).

### 13.2.3 Estimating Junction Temperature of IGBT

The junction temperature of all IGBTs operating,  $T_J$ , can be estimated with Equation (7):

$$T_J = R_{(J-C)Q} \times \{(P_{ON} + P_{SW}) \times 6\} + T_C \quad (7)$$

Where:

$R_{(J-C)Q}$  is the junction-to-case thermal resistance ( $^{\circ}\text{C}/\text{W}$ ) of all the IGBTs operating, and

$T_C$  is the case temperature ( $^{\circ}\text{C}$ ), measured at the point defined in Figure 3-2.

## 14. Performance Curves

### 14.1 Transient Thermal Resistance Curves

The following graphs represent transient thermal resistance (the ratios of transient thermal resistance), with steady-state junction-to-case thermal resistance = 1. Note that the graph representing that of the IGBT-embedded device shows only IGBT characteristics; no freewheeling diode characteristics are included.

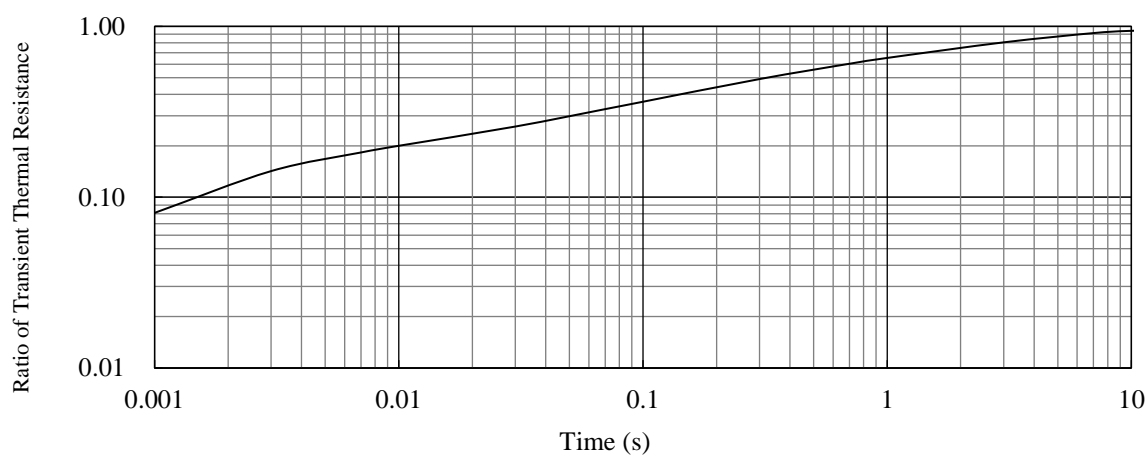


Figure 14-1. Transient Thermal Resistance: SIM2601MA

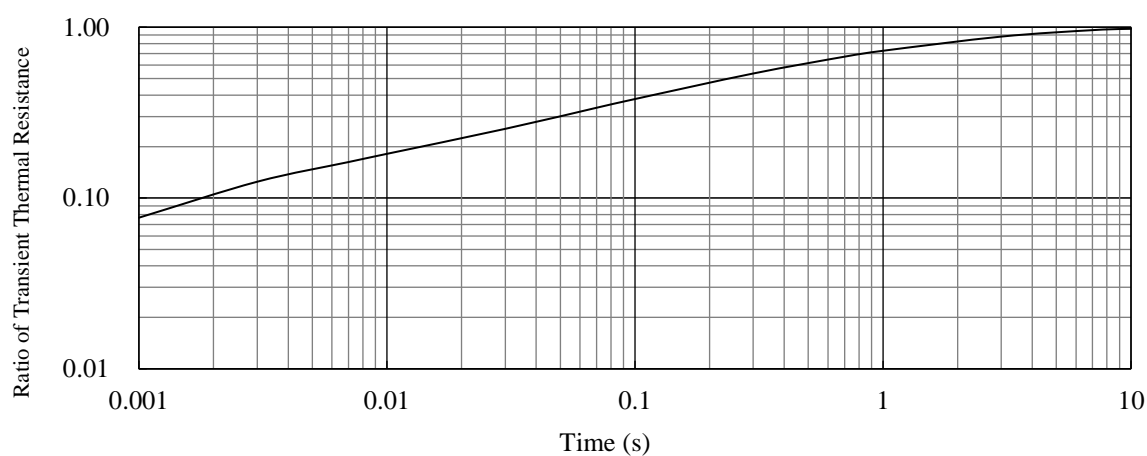


Figure 14-2. Transient Thermal Resistance: SIM2602M

## 14.2 Performance Curves of Control Parts

Figure 14-3 to Figure 14-19 provide performance curves of the control parts integrated in the SIM260xM series, including variety-dependent characteristics and thermal characteristics.  $T_J$  represents the junction temperature of the control parts.

Table 14-1. Typical Characteristics of Control Parts

Figure Number	Figure Caption
Figure 14-3	Logic Supply Current, $I_{CC}$ vs. $T_C$
Figure 14-4	Logic Supply Current, $I_{CC}$ vs. VCC Pin Voltage, $V_{CC}$
Figure 14-5	Logic Supply Current in 1-phase Operation ( $V_{SP} = 0$ V), $I_{BS}$ vs. $T_C$
Figure 14-6	Logic Supply Current in 1-phase Operation ( $V_{SP} = 5.5$ V), $I_{BS}$ vs. $T_C$
Figure 14-7	High-side Logic Operation Start Voltage, $V_{BS(ON)}$ vs. $T_C$
Figure 14-8	High-side Logic Operation Stop Voltage, $V_{BS(OFF)}$ vs. $T_C$
Figure 14-9	Low-side Logic Operation Start Voltage, $V_{CC(ON)}$ vs. $T_C$
Figure 14-10	Low-side Logic Operation Stop Voltage, $V_{CC(OFF)}$ vs. $T_C$
Figure 14-11	UVLO_VB Filtering Time vs. $T_C$
Figure 14-12	UVLO_VCC Filtering Time vs. $T_C$
Figure 14-13	High Level Input Current 1 (LA, MLP, CW/CCW, FGSEL, or VSP Pin), $I_{IN1}$ vs. $T_C$
Figure 14-14	High Level Input Current 2 (OCP Pin), $I_{IN2}$ vs. $T_C$
Figure 14-15	VREG Pin Voltage, $V_{REG}$ vs. $T_C$
Figure 14-16	Current Limit Reference Voltage, $V_{LIM}$ vs. $T_C$
Figure 14-17	OCL Blanking Time, $t_{BK(OCL)}$ + Propagation Delay, $t_D$ vs. $T_C$
Figure 14-18	OCP Threshold Voltage, $V_{TRIP}$ vs. $T_C$
Figure 14-19	OCP Hold Time, $t_P$ vs. $T_C$

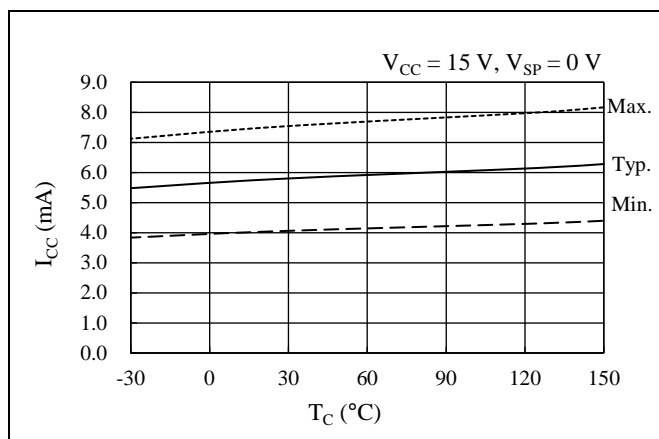


Figure 14-3. Logic Supply Current,  $I_{CC}$  vs.  $T_C$

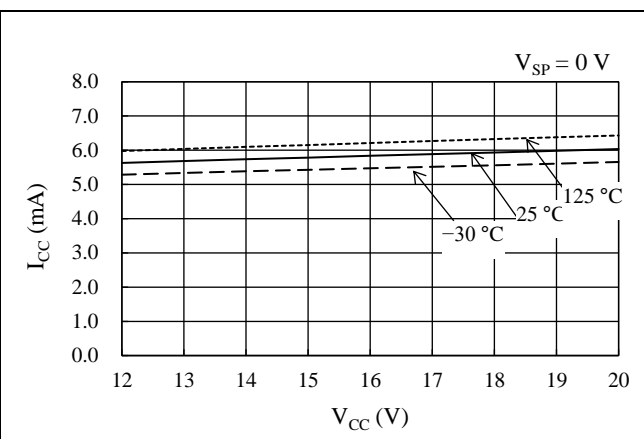


Figure 14-4. Logic Supply Current,  $I_{CC}$  vs. VCC Pin Voltage,  $V_{CC}$

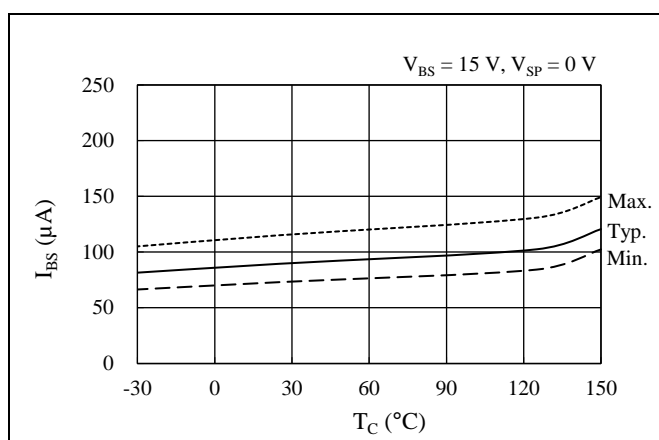


Figure 14-5. Logic Supply Current in 1-phase Operation ( $V_{SP} = 0\text{ V}$ ),  $I_{BS}$  vs.  $T_C$

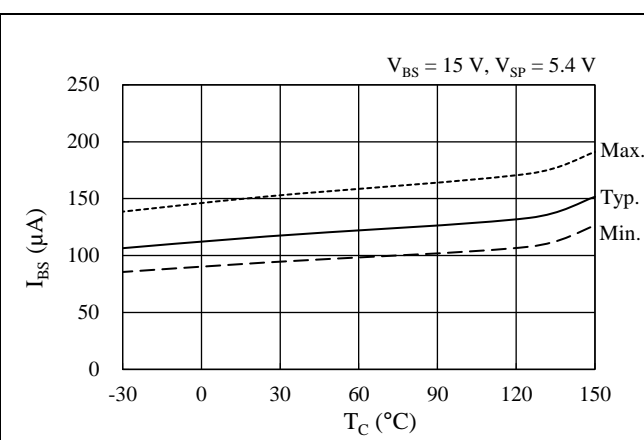


Figure 14-6. Logic Supply Current in 1-phase Operation ( $V_{SP} = 5.5\text{ V}$ ),  $I_{BS}$  vs.  $T_C$

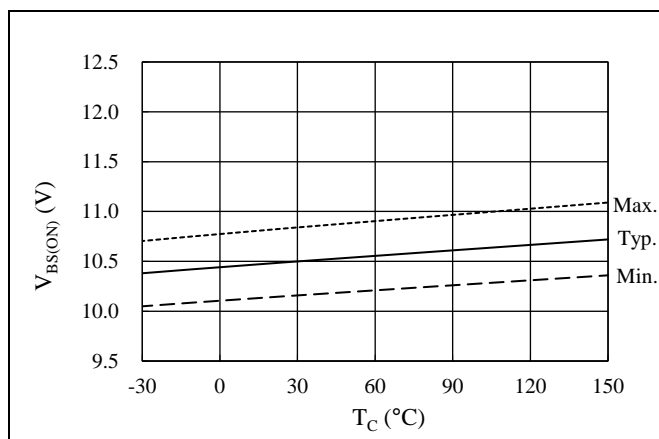


Figure 14-7. High-side Logic Operation Start Voltage,  $V_{BS(ON)}$  vs.  $T_C$

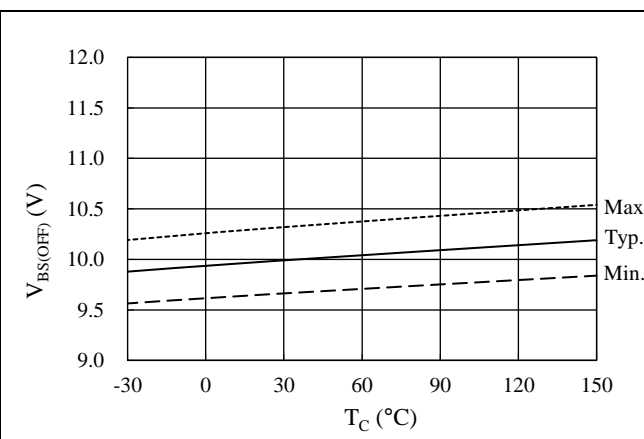


Figure 14-8. High-side Logic Operation Stop Voltage,  $V_{BS(OFF)}$  vs.  $T_C$

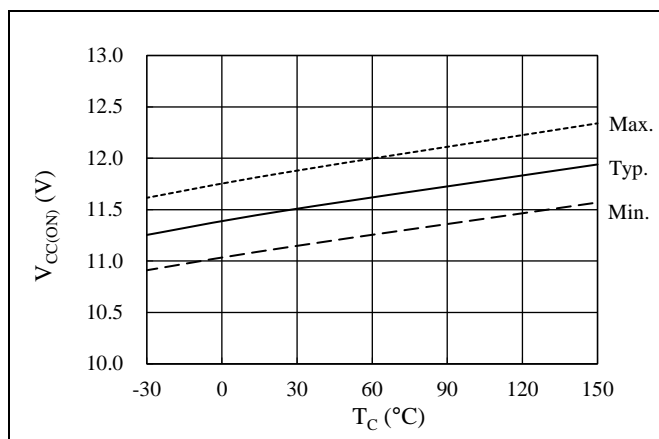


Figure 14-9. Low-side Logic Operation Start Voltage,  $V_{CC(ON)}$  vs.  $T_C$

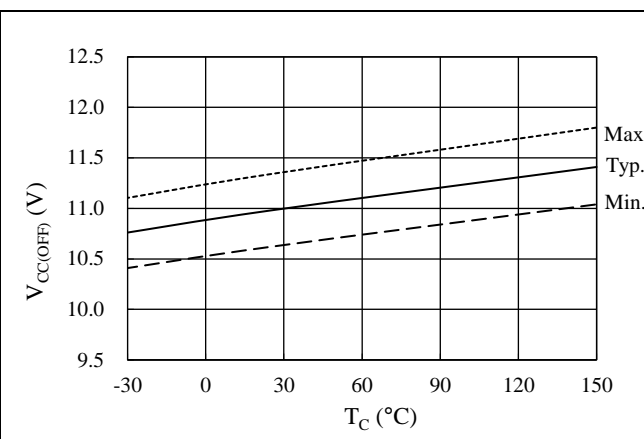


Figure 14-10. Low-side Logic Operation Stop Voltage,  $V_{CC(OFF)}$  vs.  $T_C$

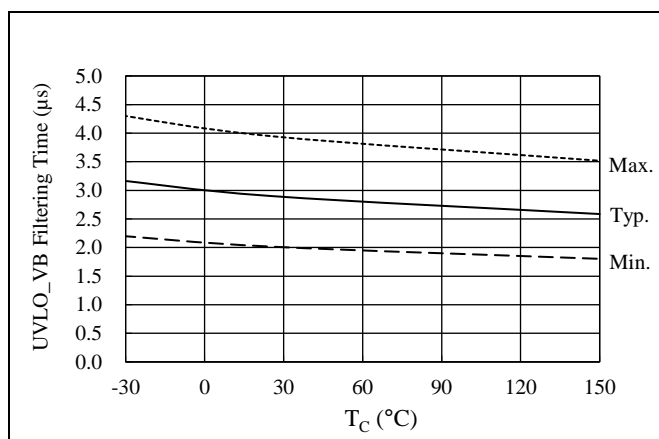


Figure 14-11. UVLO\_VB Filtering Time vs.  $T_C$

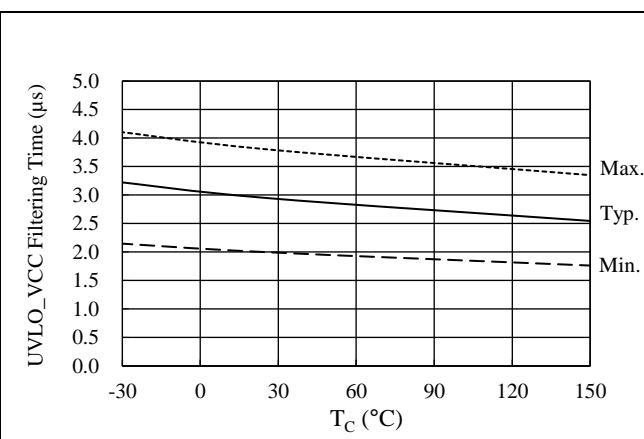


Figure 14-12. UVLO\_VCC Filtering Time vs.  $T_C$

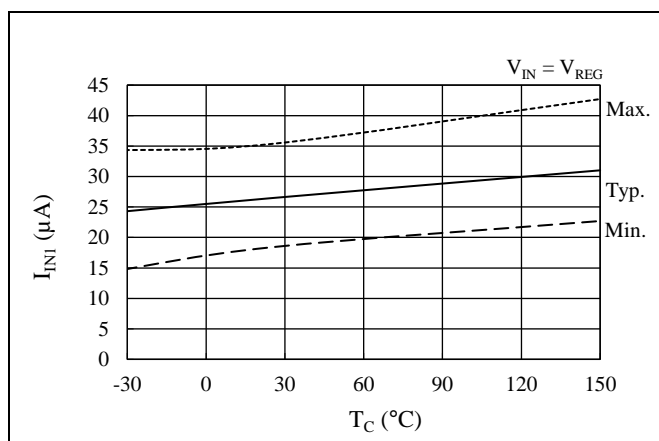


Figure 14-13. High Level Input Current 1 (LA, MLP, CW/CCW, FGSEL, or VSP Pin),  $I_{IN1}$  vs.  $T_C$

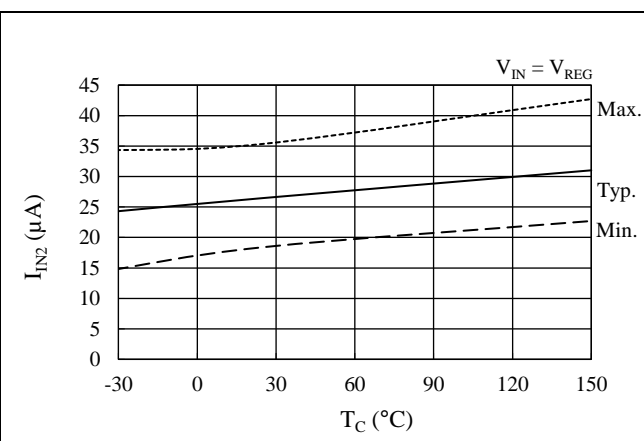


Figure 14-14. High Level Input Current 2 (OCP Pin),  $I_{IN2}$  vs.  $T_C$

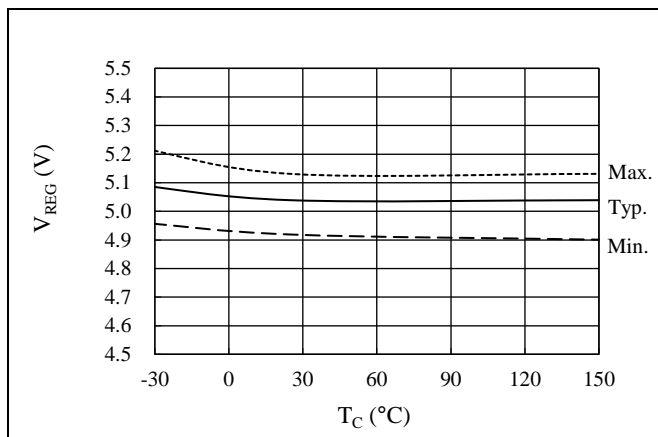


Figure 14-15. VREG Pin Voltage,  $V_{REG}$  vs.  $T_C$

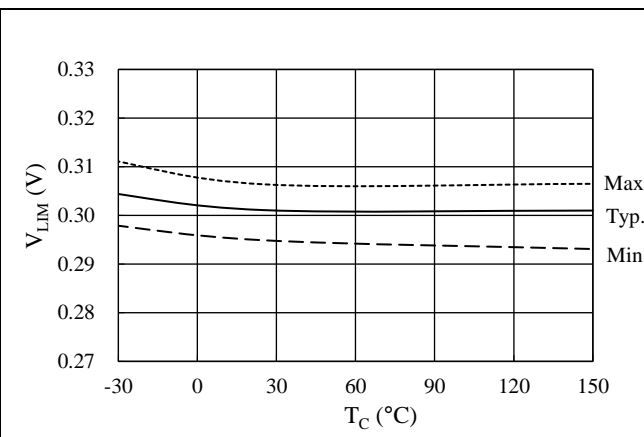


Figure 14-16. Current Limit Reference Voltage,  $V_{LIM}$  vs.  $T_C$

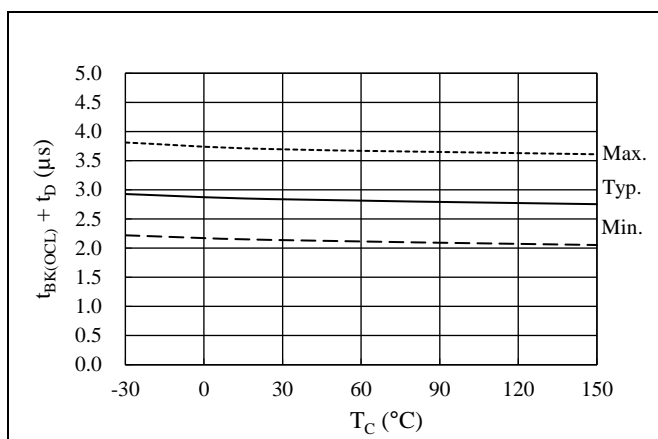


Figure 14-17. OCL Blanking Time,  $t_{BK(OCL)} + t_p$  vs.  $T_C$

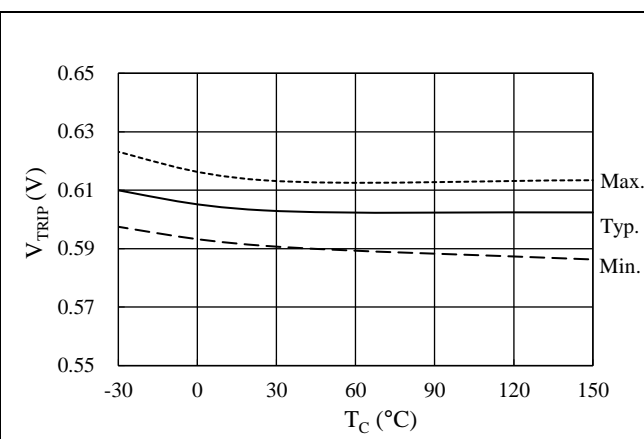


Figure 14-18. OCP Threshold Voltage,  $V_{TRIP}$  vs.  $T_C$

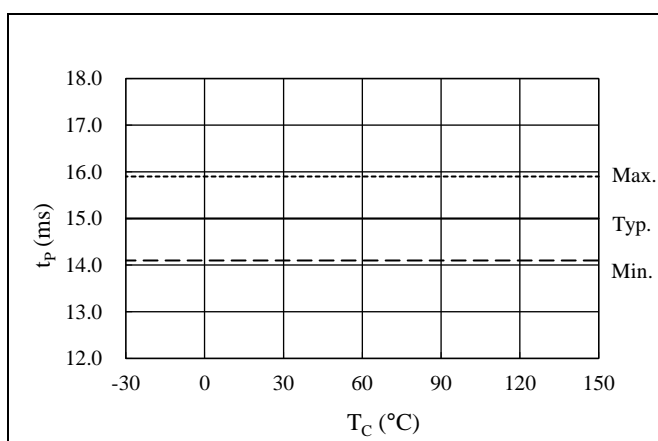


Figure 14-19. OCP Hold Time,  $t_p$  vs.  $T_C$

## 14.3 Performance Curves of Output Parts

### 14.3.1 Transistor Characteristics

#### 14.3.1.1. SIM2601MA

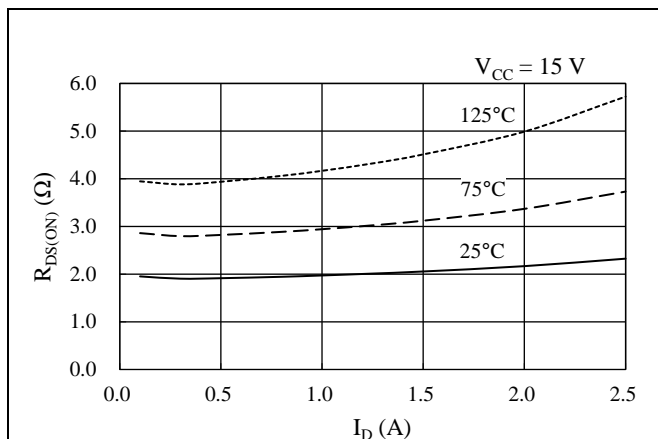


Figure 14-20. Power MOSFET  $R_{DS(ON)}$  vs.  $I_D$

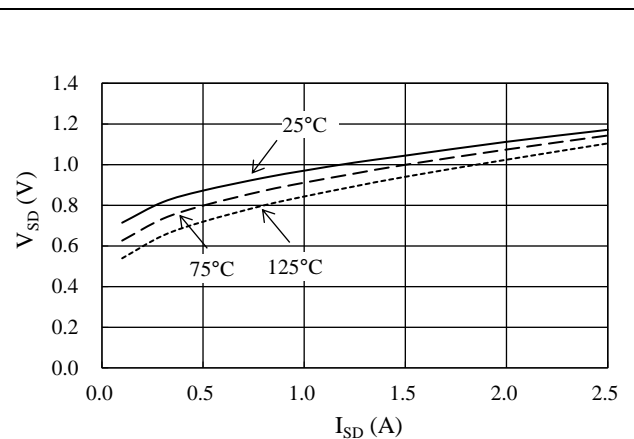


Figure 14-21. Power MOSFET  $V_{SD}$  vs.  $I_{SD}$

#### 14.3.1.2. SIM2602M

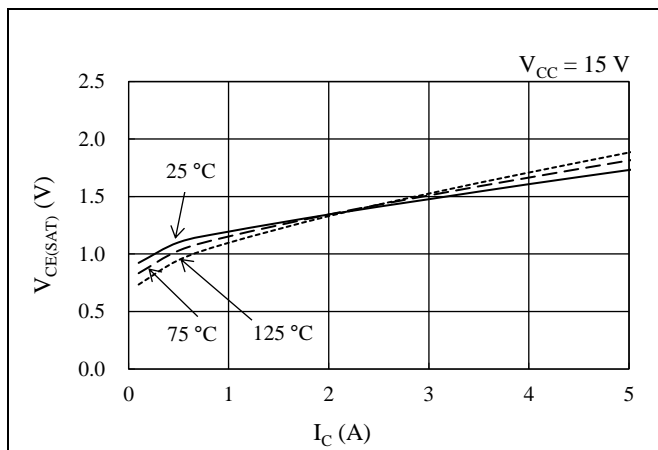


Figure 14-22. IGBT  $V_{CE(SAT)}$  vs.  $I_C$

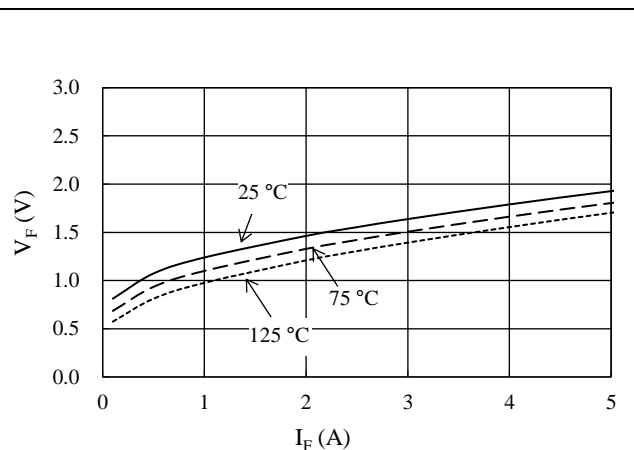


Figure 14-23. Freewheeling Diode  $V_F$  vs.  $I_F$

## 14.3.2 Switching Losses

Conditions:  $V_{Bx}$  pin voltage = 300 V, half-bridge circuit with inductive load.  
Switching Loss,  $E$ , is the sum of turn-on loss and turn-off loss.

### 14.3.2.1. SIM2601MA

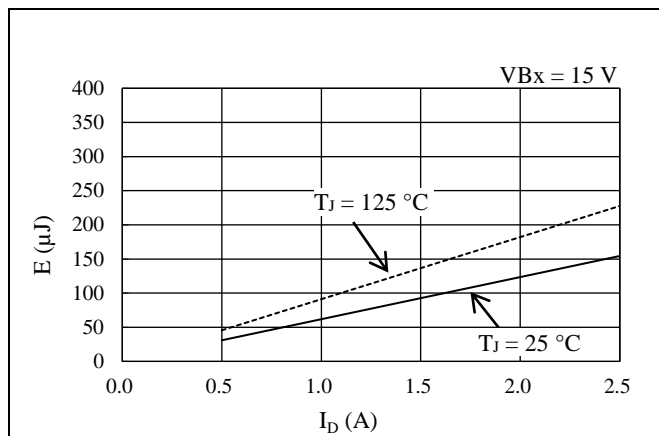


Figure 14-24. High-side Switching Loss

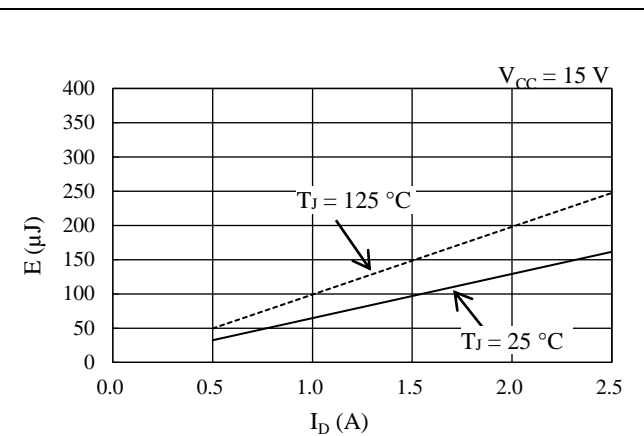


Figure 14-25. Low-side Switching Loss

### 14.3.2.2. SIM2602M

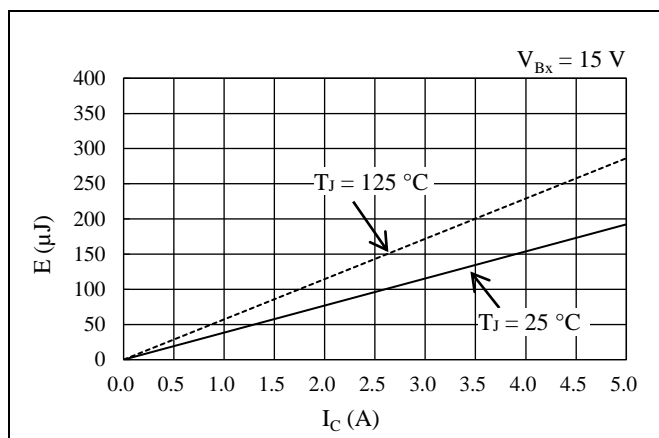


Figure 14-26. High-side Switching Loss

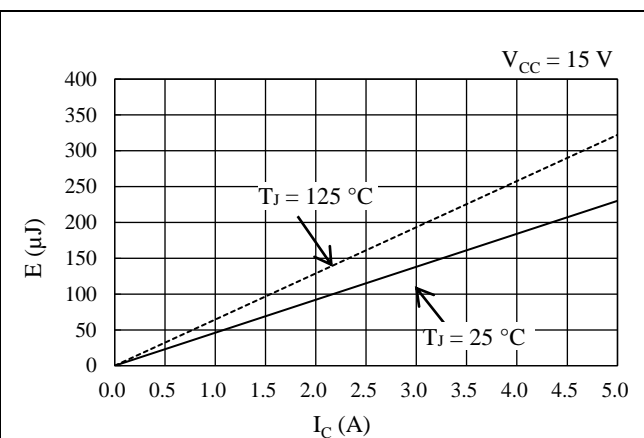


Figure 14-27. Low-side Switching Loss



## 14.4 Allowable Effective Current Curves

The following curves represent allowable effective currents in 3-phase sine-wave PWM driving with parameters such as typical  $R_{DS(ON)}$  or  $V_{CE(SAT)}$ , and typical switching losses.

Operating conditions: VBBx pin input voltage,  $V_{DC} = 300$  V; VCC pin input voltage,  $V_{CC} = 15$  V; modulation index,  $M = 0.9$ ; motor power factor,  $\cos\theta = 0.8$ ; junction temperature,  $T_J = 150$  °C.

### 14.4.1 SIM2601MA

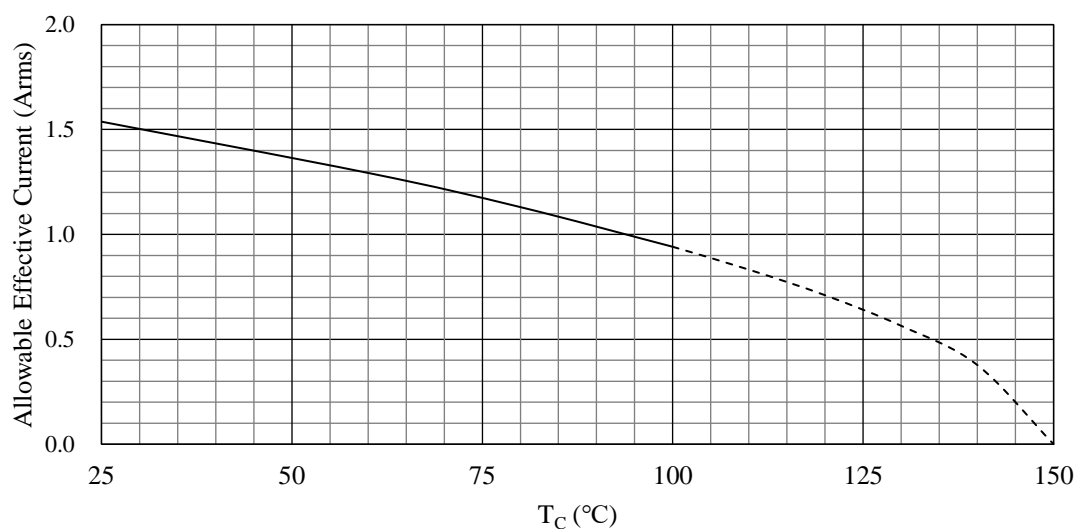


Figure 14-28. Allowable Effective Current ( $f_C = 17$  kHz): SIM2601MA

### 14.4.2 SIM2602M

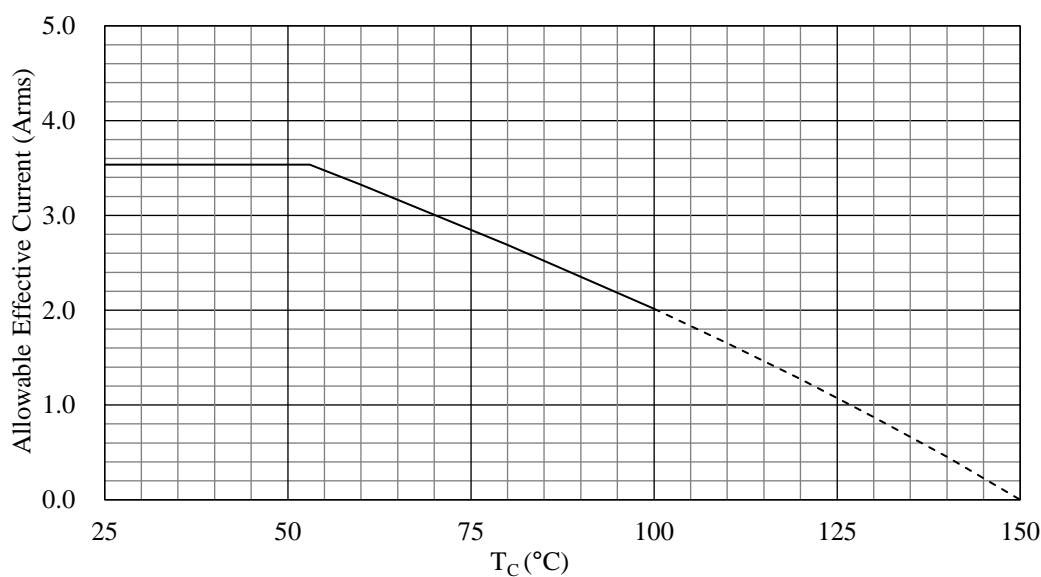


Figure 14-29. Allowable Effective Current ( $f_C = 17$  kHz): SIM2602M

**14.5 Short Circuit SOA (Safe Operating Area)**

This section provides the graph illustrating the short circuit SOA of the SIM2602M device whose output transistors consist of built-in IGBTs.

Conditions:  $V_{DC} \leq 400\text{ V}$ ,  $13.5\text{ V} \leq V_{CC} \leq 16.5\text{ V}$ ,  $T_J = 125\text{ }^{\circ}\text{C}$ , 1 pulse.

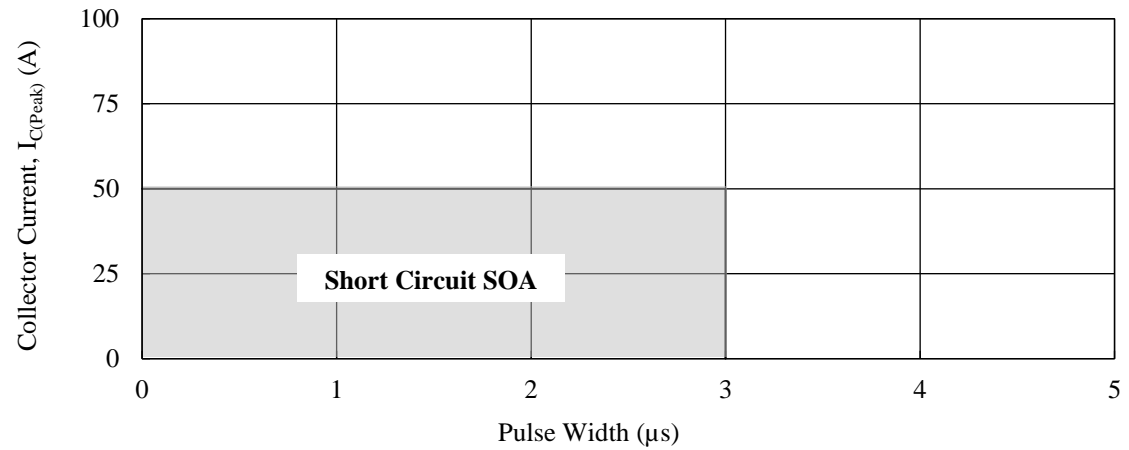
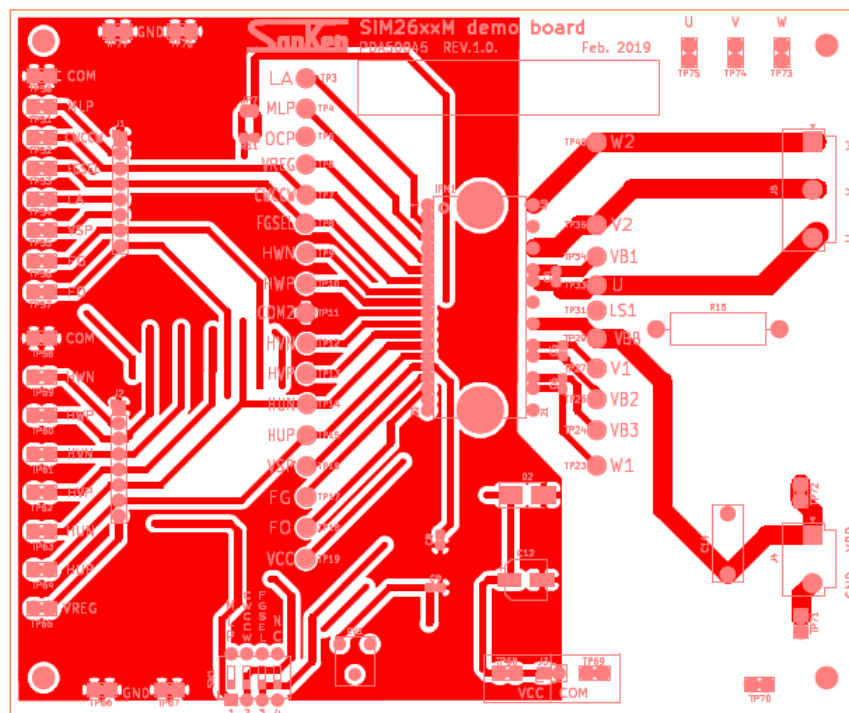


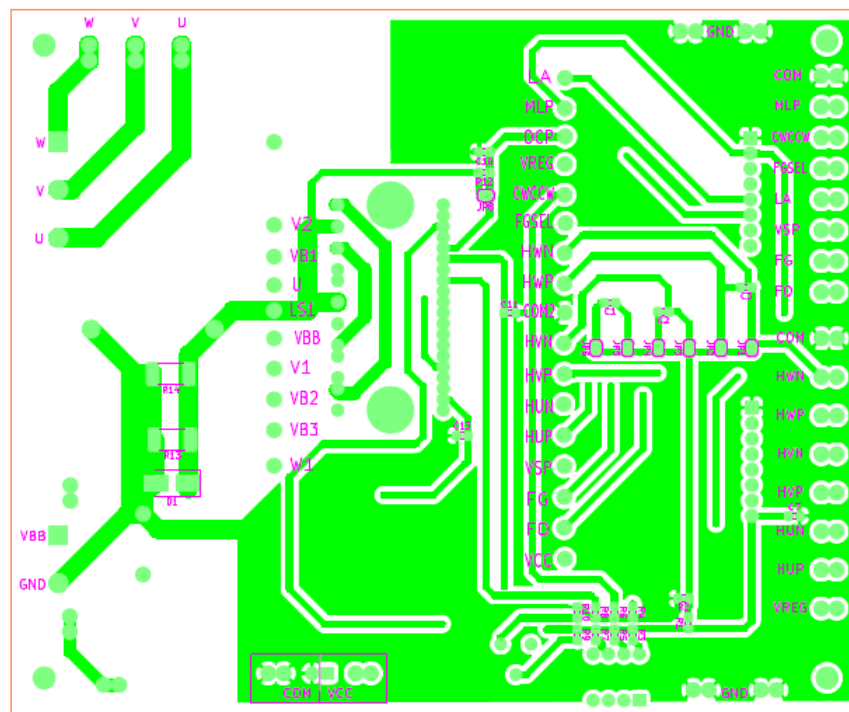
Figure 14-30. Short Circuit SOA: SIM2602M

## 15. Pattern Layout Example

This section contains the schematic diagrams of a PCB pattern layout example using an SIM260xM series device. For details on the land pattern example of the IC, see Section 9.



(Top View)



(Bottom View)

Figure 15-1. Pattern Layout Example

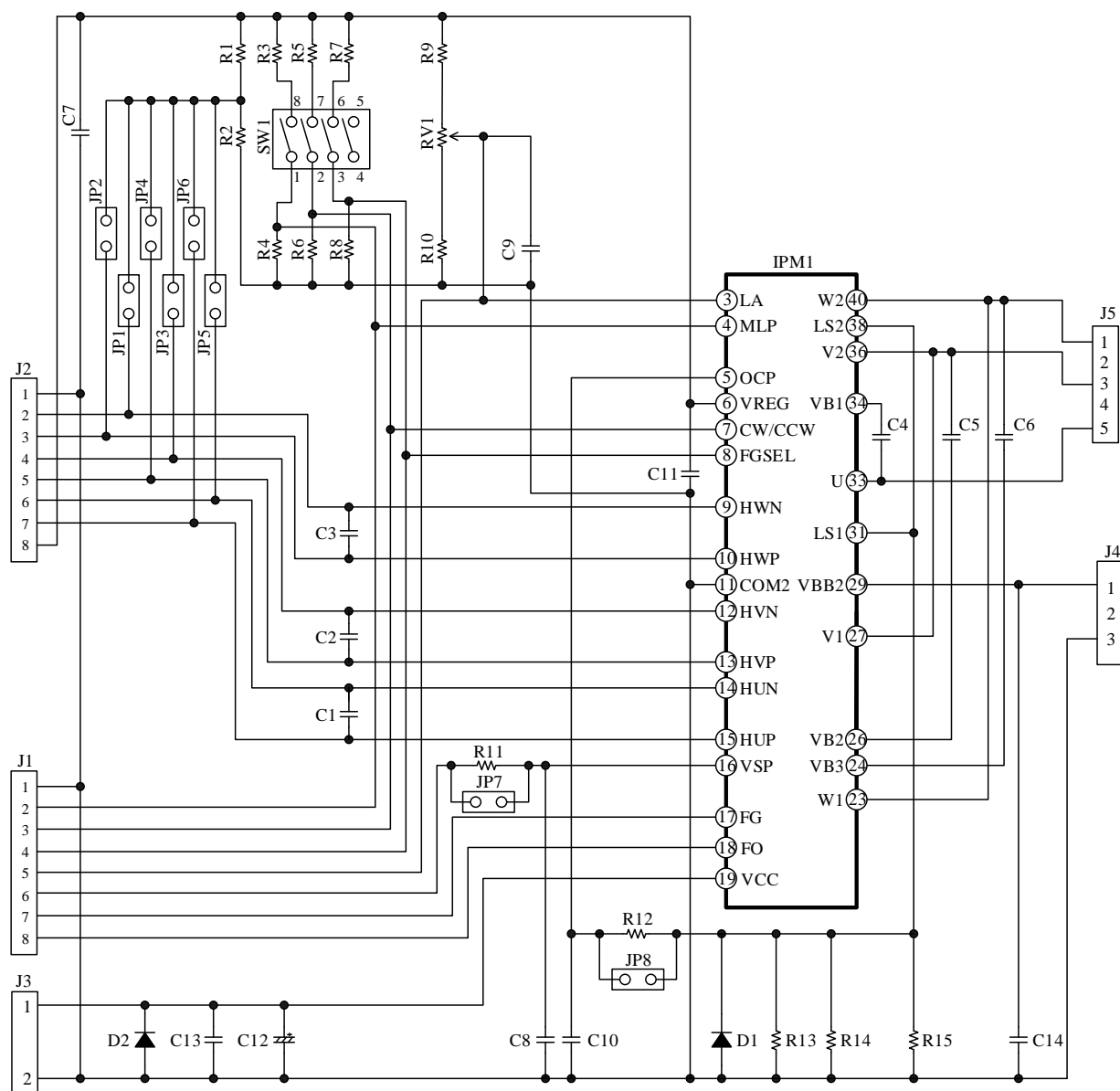


Figure 15-2. Circuit Diagram of PCB Pattern Layout Example

## 16. Typical Motor Driver Application

This section contains the information on the typical motor driver application (which uses signals input from the Hall elements) listed in the previous section, including a circuit diagram, specifications, and the bill of the materials used.

### • Motor Driver Specifications

IC	SIM2602M
Main Supply Voltage, $V_{DC}$	300 VDC (typ.)
Rated Output Power	150 W

### • Circuit Diagram

See Figure 15-2.

### • Bill of Materials

Symbol	Part Type	Ratings	Symbol	Part Type	Ratings
C1 <sup>(1)</sup>	Ceramic	Open	R6	General	Open
C2 <sup>(1)</sup>	Ceramic	Open	R7	General	Short
C3 <sup>(1)</sup>	Ceramic	Open	R8	General	Open
C4	Ceramic	1 $\mu$ F, 35 V	R9	General	Short
C5	Ceramic	1 $\mu$ F, 35 V	R10	General	1 k $\Omega$ , 0.25 W
C6	Ceramic	1 $\mu$ F, 35 V	R11 <sup>(2)</sup>	General	Open
C7	Ceramic	0.1 $\mu$ F, 35 V	R12	General	100 $\Omega$ , 0.25 W
C8	Ceramic	0.1 $\mu$ F, 35 V	R13	Metal plate	0.33 $\Omega$ , 1 W
C9	Ceramic	0.1 $\mu$ F, 35 V	R14	Metal plate	0.33 $\Omega$ , 1 W
C10	Ceramic	0.1 $\mu$ F, 35 V	R15	Metal plate	Open
C11	Ceramic	0.1 $\mu$ F, 35 V	RV1	Trimmer	10 k $\Omega$ , 0.25 W
C12	Electrolytic	100 $\mu$ F, 35 V	SW1	Switch	1 $\times$ 04
C13	Ceramic	0.1 $\mu$ F, 35 V	JP1 <sup>(3)(4)</sup>	Jumper	Open
C14	Ceramic	0.1 $\mu$ F, 630 V	JP2 <sup>(3)(4)</sup>	Jumper	Open
J1	Pin header	1 n he	JP3 <sup>(3)(4)</sup>	Jumper	Open
J2	Pin header	1 n he	JP4 <sup>(3)(4)</sup>	Jumper	Open
J3	Pin header	1 n he	JP5 <sup>(3)(4)</sup>	Jumper	Open
J4	Pin header	Equiv. to B2P3-VH	JP6 <sup>(3)(4)</sup>	Jumper	Open
J5	Pin header	Equiv. to B3P5-VH	JP7 <sup>(5)</sup>	Jumper	Short
R1	General	2.2 k $\Omega$ , 0.25 W	JP8	Jumper	Open
R2	General	2.2 k $\Omega$ , 0.25 W	D1	General	1 A, 50 V
R3	General	Short	D2	Zener	$V_Z = 20$ V, 0.5 W
R4	General	Open	IPM1	IC	SIM2602M
R5	General	Short			

<sup>(1)</sup> Refers to a noise filter capacitor for Hall element signals; should be connected as needed.

<sup>(2)</sup> Refers to a noise filter resistor for a motor speed control signal input to the VSP pin; should be connected as needed.

<sup>(3)</sup> When inputting Hall IC signals for detecting a south pole: set JP1, JP3, JP5 = short; set JP2, JP4, JP6 = open.

<sup>(4)</sup> When inputting Hall IC signals for detecting a north pole: set JP1, JP3, JP5 = open; set JP2, JP4, JP6 = short.

<sup>(5)</sup> Should be opened when R11 is connected; should be shorted when R11 is not connected.

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